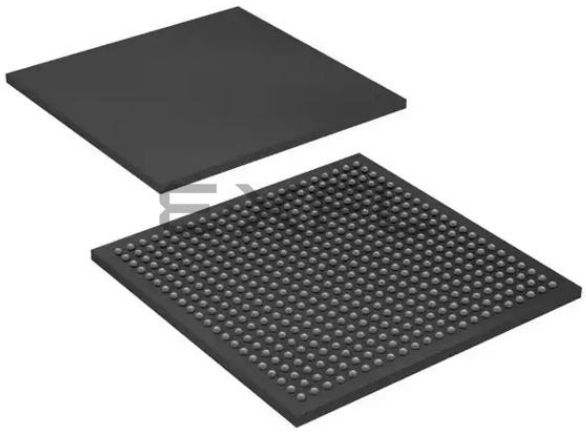

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Details	
Product Status	Active
Number of LABs/CLBs	1803
Number of Logic Elements/Cells	28848
Total RAM Bits	608256
Number of I/O	328
Number of Gates	-
Voltage - Supply	0.97V ~ 1.03V
Mounting Type	Surface Mount
Operating Temperature	-40°C ~ 100°C (TJ)
Package / Case	484-BGA
Supplier Device Package	484-FBGA (23x23)
Purchase URL	https://www.e-xfl.com/product-detail/intel/ep4ce30f23i8l

Table 5–6. Cyclone IV E PLL Features (Part 2 of 2)

Hardware Features	Availability
Loss of lock detection	✓

Notes to Table 5–6:

(1) C counters range from 1 through 512 if the output clock uses a 50% duty cycle. For any output clocks using a non-50% duty cycle, the post-scale counters range from 1 through 256.

(2) Only applicable if the input clock jitter is in the input jitter tolerance specifications.

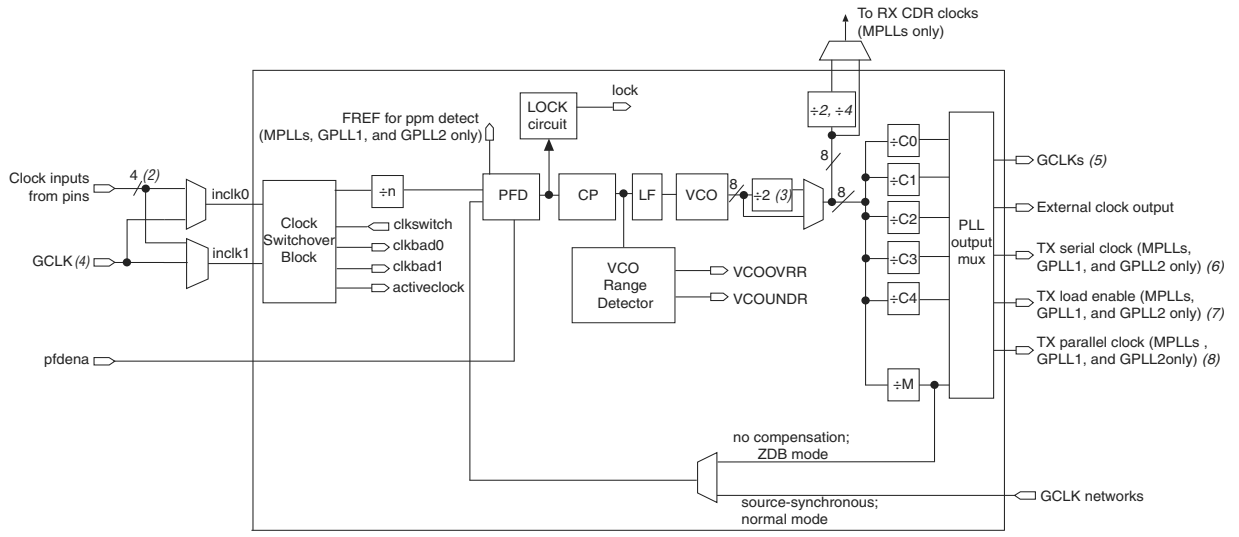
(3) The smallest phase shift is determined by the VCO period divided by eight. For degree increments, Cyclone IV E devices can shift all output frequencies in increments of at least 45°. Smaller degree increments are possible depending on the frequency and divide parameters.

Cyclone IV PLL Hardware Overview

This section gives a hardware overview of the Cyclone IV PLL.

Figure 5–9 shows a simplified block diagram of the major components of the PLL of Cyclone IV GX devices.

Figure 5–9. Cyclone IV GX PLL Block Diagram (1)



Notes to Figure 5–9:

(1) Each clock source can come from any of the four clock pins located on the same side of the device as the PLL.

(2) There are additional 4 pairs of dedicated differential clock inputs in EP4CGX50, EP4CGX75, EP4CGX110, and EP4CGX150 devices that can only drive general purpose PLLs and multipurpose PLLs on the left side of the device. `CLK[19..16]` can access `PLL_2`, `PLL_6`, `PLL_7`, and `PLL_8` while `CLK[23..20]` can access `PLL_1`, `PLL_5`, `PLL_6`, and `PLL_7`. For the location of these clock input pins, refer to Figure 5–3 on page 5–13.

(3) This is the VCO post-scale counter K.

(4) This input port is fed by a pin-driven dedicated GCLK, or through a clock control block if the clock control block is fed by an output from another PLL or a pin-driven dedicated GCLK. An internally generated global signal cannot drive the PLL.

(5) For the general purpose PLL and multipurpose PLL counter outputs connectivity to the GCLKs, refer to Table 5–1 on page 5–2 and Table 5–2 on page 5–4.

(6) Only the CI output counter can drive the TX serial clock.

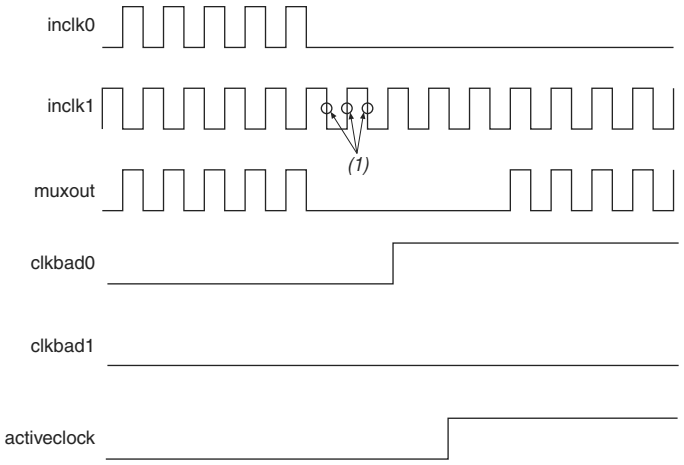
(7) Only the C2 output counter can drive the TX load enable.

(8) Only the C3 output counter can drive the TX parallel clock.

20%. This feature is useful when clock sources can originate from multiple cards on the backplane, requiring a system-controlled switchover between frequencies of operation. Choose the secondary clock frequency so the VCO operates in the recommended frequency range. Also, set the M, N, and C counters accordingly to keep the VCO operating frequency in the recommended range.

Figure 5–18 shows a waveform example of the switchover feature when using automatic loss of clock detection. Here, the `inclk0` signal remains low. After the `inclk0` signal remains low for approximately two clock cycles, the clock-sense circuitry drives the `clkbad0` signal high. Also, because the reference clock signal is not toggling, the switchover state machine controls the multiplexer through the `clksw` signal to switch to `inclk1`.

Figure 5–18. Automatic Switchover Upon Clock Loss Detection *(1)*



Note to Figure 5–18:

(1) Switchover is enabled on the falling edge of `inclk0` or `inclk1`, depending on which clock is available. In this figure, switchover is enabled on the falling edge of `inclk1`.

Manual Override

If you are using the automatic switchover, you must switch input clocks with the manual override feature with the `clkswitch` input.

Figure 5–19 shows an example of a waveform illustrating the switchover feature when controlled by `clkswitch`. In this case, both clock sources are functional and `inclk0` is selected as the reference clock. A low-to-high transition of the `clkswitch` signal starts the switchover sequence. The `clkswitch` signal must be high for at least three clock cycles (at least three of the longer clock period if `inclk0` and `inclk1` have different frequencies). On the falling edge of `inclk0`, the reference clock of the counter, `muxout`, is gated off to prevent any clock glitching. On the falling edge of `inclk1`, the reference clock multiplexer switches from `inclk0` to `inclk1` as the PLL reference, and the `activeclock` signal changes to indicate which clock is currently feeding the PLL.

For the specific sustaining current for each V_{CCIO} voltage level driven through the resistor and for the overdrive current used to identify the next driven input level, refer to the *Cyclone IV Device Datasheet* chapter.

Programmable Pull-Up Resistor

Each Cyclone IV device I/O pin provides an optional programmable pull-up resistor while in user mode. If you enable this feature for an I/O pin, the pull-up resistor holds the output to the V_{CCIO} level of the output pin's bank.

If you enable the programmable pull-up resistor, the device cannot use the bus-hold feature. Programmable pull-up resistors are not supported on the dedicated configuration, JTAG, and dedicated clock pins.

When the optional `DEV_OE` signal drives low, all I/O pins remains tri-stated even with the programmable pull-up option enabled.

Programmable Delay

The Cyclone IV IOE includes programmable delays to ensure zero hold times, minimize setup times, increase clock-to-output times, and delay the clock input signal.

A path in which a pin directly drives a register may require a programmable delay to ensure zero hold time, whereas a path in which a pin drives a register through combinational logic may not require the delay. Programmable delays minimize setup time. The Quartus II Compiler can program these delays to automatically minimize setup time while providing a zero hold time. Programmable delays can increase the register-to-pin delays for output registers. Each dual-purpose clock input pin provides a programmable delay to the global clock networks.

Table 6–1 shows the programmable delays for Cyclone IV devices.

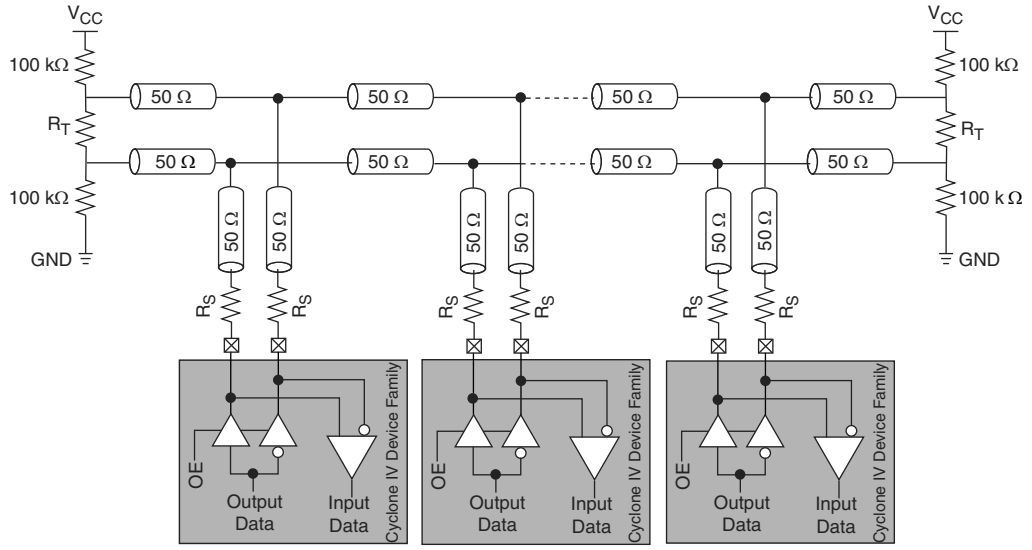
Table 6–1. Cyclone IV Devices Programmable Delay Chain

Programmable Delay	Quartus II Logic Option
Input pin-to-logic array delay	Input delay from pin to internal cells
Input pin-to-input register delay	Input delay from pin to input register
Output pin delay	Delay from output register to output pin
Dual-purpose clock input pin delay	Input delay from dual-purpose clock pin to fan-out destinations

There are two paths in the IOE for an input to reach the logic array. Each of the two paths can have a different delay. This allows you to adjust delays from the pin to the internal logic element (LE) registers that reside in two different areas of the device. You must set the two combinational input delays with the input delay from pin to internal cells logic option in the Quartus II software for each path. If the pin uses the input register, one of the delays is disregarded and the delay is set with the input delay from pin to input register logic option in the Quartus II software.

Figure 6–14 shows a typical BLVDS topology with multiple transmitter and receiver pairs.

Figure 6–14. BLVDS Topology with Cyclone IV Devices Transmitters and Receivers



The BLVDS I/O standard is supported on the top, bottom, and right I/O banks of Cyclone IV devices. The BLVDS transmitter uses two single-ended output buffers with the second output buffer programmed as inverted, while the BLVDS receiver uses a true LVDS input buffer. The transmitter and receiver share the same pins. An output-enabled (OE) signal is required to tristate the output buffers when the LVDS input buffer receives a signal.

For more information, refer to the *Cyclone IV Device Datasheet* chapter.

Designing with BLVDS

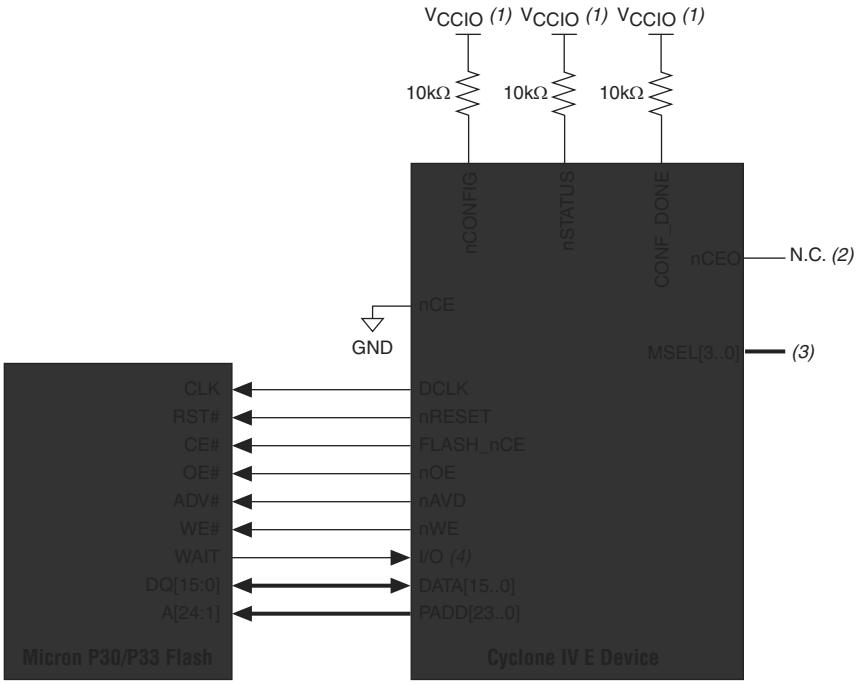
The BLVDS bidirectional communication requires termination at both ends of the bus in BLVDS. The termination resistor (R_T) must match the bus differential impedance, which in turn depends on the loading on the bus. Increasing the load decreases the bus differential impedance. With termination at both ends of the bus, termination is not required between the two signals at the input buffer. A single series resistor (R_S) is required at the output buffer to match the output buffer impedance to the transmission line impedance. However, this series resistor affects the voltage swing at the input buffer. The maximum data rate achievable depends on many factors.

Altera recommends that you perform simulation using the IBIS model while considering factors such as bus loading, termination values, and output and input buffer location on the bus to ensure that the required performance is achieved.

For more information about BLVDS interface support in Altera devices, refer to *AN 522: Implementing Bus LVDS Interface in Supported Altera Device Families*.

Figure 8–7 shows the interface for the Micron P30 flash memory and P33 flash memory to the Cyclone IV E device pins.

Figure 8–7. Single-Device AP Configuration Using Micron P30 and P33 Flash Memory



Notes to Figure 8–7:

(1) Connect the pull-up resistors to the V_{CCIO} supply of the bank in which the pin resides.

(2) The nCEO pin is left unconnected or used as a user I/O pin when it does not feed the nCE pin of another device.

(3) The MSEL pin settings vary for different configuration voltage standards and POR time. To connect MSEL[3..0], refer to Table 8–5 on page 8–9. Connect the MSEL pins directly to V_{CCA} or GND.

(4) AP configuration ignores the WAIT signal during configuration mode. However, if you are accessing flash during user mode with user logic, you can optionally use normal I/O to monitor the WAIT signal from the Micron P30 or P33 flash.

☞ To tri-state the configuration bus for AP configuration schemes, you must tie nCE high and nCONFIG low.

☞ In a single-device AP configuration, the maximum board loading and board trace length between supported parallel flash and Cyclone IV E devices must follow the recommendations listed in Table 8–11 on page 8–28.

☞ If you use the AP configuration scheme for Cyclone IV E devices, the V_{CCIO} of I/O banks 1, 6, 7, and 8 must be 3.3, 3.0, 2.5, or 1.8 V. Altera does not recommend using the level shifter between the Micron P30 or P33 flash and the Cyclone IV E device in the AP configuration scheme.

Device Configuration Pins

Table 8–18 through Table 8–21 describe the connections and functionality of all the configuration related pins on Cyclone IV devices. Table 8–18 and Table 8–19 list the device pin configuration for the Cyclone IV GX and Cyclone IV E, respectively.

Table 8–18. Configuration Pin Summary for Cyclone IV GX Devices

Bank	Description	Input/Output	Dedicated	Powered By	Configuration Mode
8	Data[4:2]	Input	—	V_{CCIO}	FPP
3	Data[7:5]	Input	—	V_{CCIO}	FPP
9	nCSO (2)	Output	—	V_{CCIO}	AS
3	CRC_ERROR	Output	—	V_{CCIO}/Pull-up (1)	Optional, all modes
9	DATA[0] (2)	Input	Yes	V_{CCIO}	PS, FPP, AS
9	DATA[1]/ASDO (2)	Input	—	V_{CCIO}	FPP
		Output		V_{CCIO}	AS
3	INIT_DONE	Output	—	Pull-up	Optional, all modes
3	nSTATUS	Bidirectional	Yes	Pull-up	All modes
9	nCE	Input	Yes	V_{CCIO}	All modes
9	DCLK (2)	Input	Yes	V_{CCIO}	PS, FPP
		Output		V_{CCIO}	AS
3	CONF_DONE	Bidirectional	Yes	Pull-up	All modes
9	TDI	Input	Yes	V_{CCIO}	JTAG
9	TMS	Input	Yes	V_{CCIO}	JTAG
9	TCK	Input	Yes	V_{CCIO}	JTAG
9	nCONFIG	Input	Yes	V_{CCIO}	All modes
8	CLKUSR	Input	—	V_{CCIO}	Optional
3	nCEO	Output	—	V_{CCIO}	Optional, all modes
3	MSEL	Input	Yes	V_{CCINT}	All modes
9	TDO	Output	Yes	V_{CCIO}	JTAG
6	DEV_OE	Input	—	V_{CCIO}	Optional
6	DEV_CLRn	Input	—	V_{CCIO}	Optional

Notes to Table 8–18:

(1) The CRC_ERROR pin is a dedicated open-drain output or an optional user I/O pin. Active high signal indicates that the error detection circuit has detected errors in the configuration SRAM bits. This pin is optional and is used when the CRC error detection circuit is enabled in the Quartus II software from the **Error Detection CRC** tab of the **Device and Pin Options** dialog box. When using this pin, connect it to an external 10-kΩ pull-up resistor to an acceptable voltage that satisfies the input voltage of the receiving device.

(2) To tri-state AS configuration pins in the AS configuration scheme, turn on the **Enable input tri-state on active configuration pins in user mode** option from the **Device and Pin Options** dialog box. This tri-states DCLK, nCSO, Data[0], and Data[1]/ASDO pins. Dual-purpose pins settings for these pins are ignored. To set these pins to different settings, turn off the **Enable input tri-state on active configuration pins in user mode** option and set the desired setting from the Dual-purpose Pins Setting menu.

Table 8–19. Configuration Pin Summary for Cyclone IV E Devices (Part 1 of 3)

Bank	Description	Input/Output	Dedicated	Powered By	Configuration Mode
1	nCSO (1) FLASH_nCE (2)	Output	—	V_{CCIO}	AS, AP
6	CRC_ERROR (3)	Output	—	V_{CCIO}/Pull-up (4)	Optional, all modes

When Cyclone IV devices successfully load the application configuration, they enter user mode. In user mode, the soft logic (the Nios II processor or state machine and the remote communication interface) assists the Cyclone IV device in determining when a remote system update is arriving. When a remote system update arrives, the soft logic receives the incoming data, writes it to the configuration memory device and triggers the device to load the factory configuration. The factory configuration reads the remote system upgrade status register, determines the valid application configuration to load, writes the remote system upgrade control register accordingly, and starts system reconfiguration.

The remote system upgrade status register is updated by the dedicated error monitoring circuitry after an error condition, but before the factory configuration is loaded.

Table 8–26. Control Register Contents After an Error or Reconfiguration Trigger Condition

Reconfiguration Error/Trigger	Control Register Setting In Remote Update
nCONFIG reset	All bits are 0
nSTATUS error	All bits are 0
CORE triggered reconfiguration	Update register
CRC error	All bits are 0
Wd time out	All bits are 0

User Watchdog Timer

The user watchdog timer prevents a faulty application configuration from indefinitely stalling the device. The system uses the timer to detect functional errors after an application configuration is successfully loaded into the Cyclone IV device.

The user watchdog timer is a counter that counts down from the initial value loaded into the remote system upgrade control register by the factory configuration. The counter is 29 bits wide and has a maximum count value of 2^{29}. When specifying the user watchdog timer value, specify only the most significant 12 bits. The remote system upgrade circuitry appends 17'b1000 to form the 29-bits value for the watchdog timer. The granularity of the timer setting is 2^{17} cycles. The cycle time is based on the frequency of the 10-MHz internal oscillator or CLKUSR (maximum frequency of 40 MHz).

Table 8–27 lists the operating range of the 10-MHz internal oscillator.

Table 8–27. 10-MHz Internal Oscillator Specifications

Minimum	Typical	Maximum	Unit
5	6.5	10	MHz

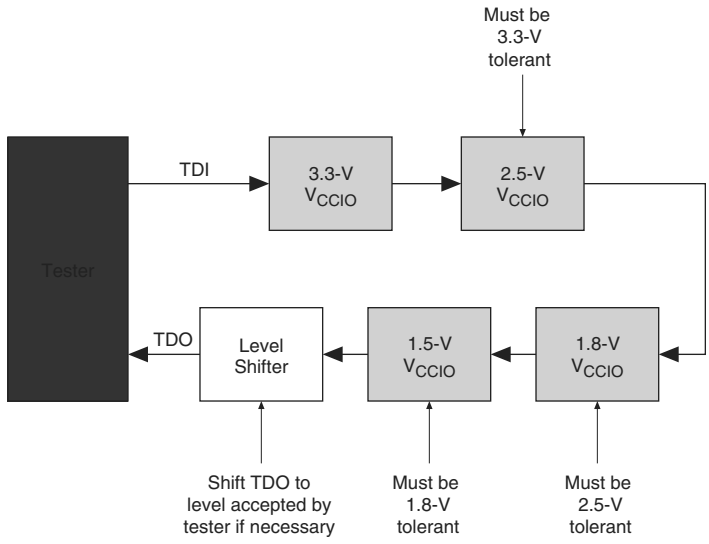
The user watchdog timer begins counting after the application configuration enters device user mode. This timer must be periodically reloaded or reset by the application configuration before the timer expires by asserting RU_nRSTIMER. If the application configuration does not reload the user watchdog timer before the count expires, a time-out signal is generated by the remote system upgrade dedicated circuitry. The time-out signal tells the remote system upgrade circuitry to set the user watchdog timer status bit (Wd) in the remote system upgrade status register and reconfigures the device by loading the factory configuration.

To allow the remote system upgrade dedicated circuitry to reset the watchdog timer, you must assert the RU_nRSTIMER signal active for a minimum of 250 ns. This is equivalent to strobing the reset_timer input of the ALTREMOTE_UPDATE megafunction high for a minimum of 250 ns.

Errors during configuration are detected by the CRC engine. Functional errors must not exist in the factory configuration because it is stored and validated during production and is never updated remotely.

Figure 10–3 shows the JTAG chain of mixed voltages and how a level shifter is inserted in the chain.

Figure 10–3. JTAG Chain of Mixed Voltages



Boundary-Scan Description Language Support

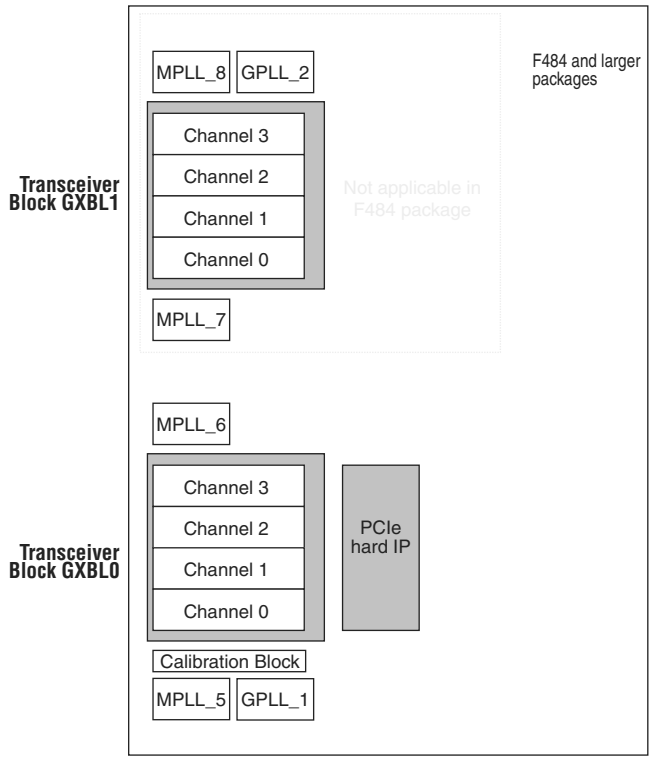
The boundary-scan description language (BSDL), a subset of VHDL, provides a syntax that allows you to describe the features of an IEEE Std. 1149.1/IEEE Std. 1149.6 BST-capable device that can be tested.

For more information about how to download BSDL files for IEEE Std. 1149.1-compliant Cyclone IV E devices, refer to *IEEE Std. 1149.1 BSDL Files*.

For more information about how to download BSDL files for IEEE Std. 1149.6-compliant Cyclone IV GX devices, refer to *IEEE Std. 1149.6 BSDL Files*.

You can also generate BSDL files (pre-configuration and post-configuration) for IEEE Std. 1149.1/IEEE Std. 1149.6-compliant Cyclone IV devices with the Quartus® II software version 9.1 SP1 and later. For more information about the procedure to generate BSDL files using the Quartus II software, refer to *BSDL Files Generation in Quartus II*.

Figure 1–2. F484 and Larger Packages with Transceiver Channels for Cyclone IV GX Devices



For more information about the transceiver architecture, refer to the following sections:

- "Architectural Overview" on page 1–4
- "Transmitter Channel Datapath" on page 1–5
- "Receiver Channel Datapath" on page 1–11
- "Transceiver Clocking Architecture" on page 1–26
- "Transceiver Channel Datapath Clocking" on page 1–29
- "FPGA Fabric-Transceiver Interface Clocking" on page 1–43
- "Calibration Block" on page 1–45
- "PCI-Express Hard IP Block" on page 1–46

Word Aligner

Figure 1–16 shows the word aligner block diagram. The word aligner receives parallel data from the deserializer and restores the word boundary based on a pre-defined alignment pattern that must be received during link synchronization. The word aligner supports three operational modes as listed in Table 1–3.

Figure 1–16. Word Aligner Block Diagram

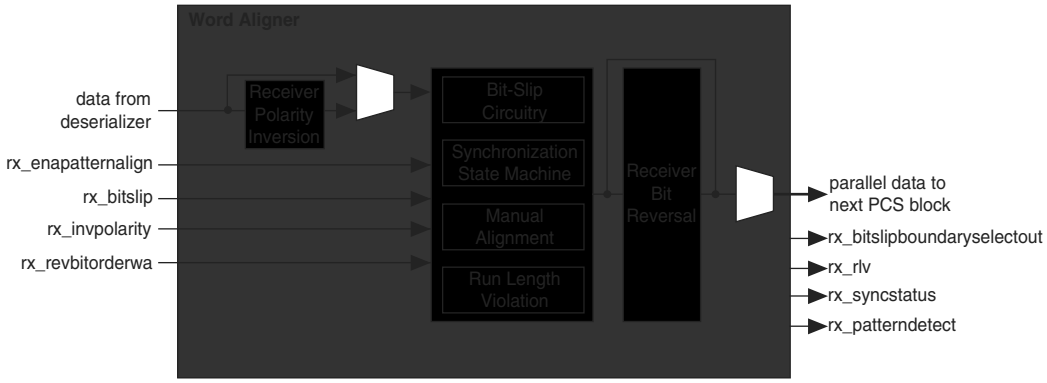


Table 1–3. Word Aligner Modes

Modes	PMA-PCS Interface Widths	Allowed Word Alignment Pattern Lengths
Manual Alignment	8-bit	16 bits
	10-bit	7 or 10 bits
Bit-Slip	8-bit	16 bits
	10-bit	7 or 10 bits
Automatic Synchronization State Machine	10-bit	7 or 10 bits

Manual Alignment Mode

In manual alignment mode, the `rx_enapatternalign` port controls the word aligner with either an 8- or 10-bit data width setting.

The 8-bit word aligner is edge-sensitive to the `rx_enapatternalign` signal. A rising edge on `rx_enapatternalign` signal after deassertion of the `rx_digitalreset` signal triggers the word aligner to look for the word alignment pattern in the received data stream. It updates the word boundary if it finds the word alignment pattern in a new word boundary. Any word alignment pattern received thereafter in a different word boundary causes the word aligner to re-align to the new word boundary only if there is a rising edge in the `rx_enapatternalign` signal.

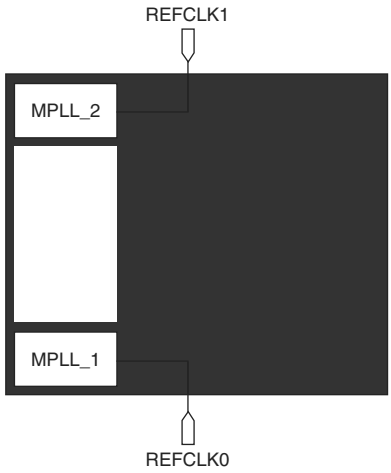
The 10-bit word aligner is level-sensitive to the `rx_enapatternalign` signal. The word aligner looks for the programmed 7-bit or 10-bit word alignment pattern or its complement in the received data stream, if the `rx_enapatternalign` signal is held high. It updates the word boundary if it finds the word alignment pattern in a new word boundary. If the `rx_enapatternalign` signal is deasserted, the word aligner maintains the current word boundary even when it receives the word alignment pattern in a new word boundary.

Input Reference Clocking

When used for transceiver, the left PLLs synthesize the input reference clock to generate the required clocks for the transceiver channels. Figure 1–25 and Figure 1–26 show the sources of input reference clocks for PLLs used in the transceiver operation.

☞ Clock output from PLLs in the FPGA core cannot feed into PLLs used by the transceiver as input reference clock.

Figure 1–25. PLL Input Reference Clocks in Transceiver Operation for F324 and Smaller Packages (1), (2)



Notes to Figure 1–25:

(1) The REFCLK0 and REFCLK1 pins are dual-purpose CLK, REFCLK, or DIFFCLK pins that reside in banks 3A and 8A respectively.

(2) Using any clock input pins other than the designated REFCLK pins as shown here to drive the MPLLs may have reduced jitter performance.

☞ In any configuration, a receiver channel cannot source CDR clocks from other PLLs beyond the two multipurpose PLLs directly adjacent to transceiver block where the channel resides.

The Cyclone IV GX transceivers support non-bonded (×1) and bonded (×2 and ×4) channel configurations. The two configurations differ in regards to clocking and phase compensation FIFO control. Bonded configuration provides a relatively lower channel-to-channel skew between the bonded channels than in non-bonded configuration. Table 1–8 lists the supported conditions in non-bonded and bonded channel configurations.

Table 1–8. Supported Conditions in Non-Bonded and Bonded Channel Configurations

Channel Configuration	Description	Supported Channel Operation Mode
Non-bonded (×1)	■ Low-speed clock in each channel is sourced independently ■ Phase compensation FIFO in each channel has its own pointers and control logic	■ Transmitter Only ■ Receiver Only ■ Transmitter and Receiver
Bonded (×2 and ×4)	■ Low-speed clock in each bonded channel is sourced from a common bonded clock path for lower channel-to-channel skew ■ Phase compensation FIFOs in bonded channels share common pointers and control logic for equal latency through the FIFOs in all bonded channels ■ ×2 bonded configuration is supported with channel 0 and channel 1 in a transceiver block ■ ×4 bonded configuration is supported with all four channels in a transceiver block	■ Transmitter Only ■ Transmitter and Receiver

Non-Bonded Channel Configuration

In non-bonded channel configuration, the high- and low-speed clocks for each channel are sourced independently. The phase compensation FIFOs in each channel has its own pointers and control logic. When implementing multi-channel serial interface in non-bonded channel configuration, the clock skew and unequal latency results in larger channel-to-channel skew.

☞ Altera recommends using bonded channel configuration (×2 or ×4) when implementing multi-channel serial interface for a lower channel-to-channel skew.

In a transceiver block, the high- and low-speed clocks for each channel are distributed primarily from one of the two multipurpose PLLs directly adjacent to the block. Transceiver channels for devices in F484 and larger packages support additional clocking flexibility. In these packages, some channels support high-speed and low-speed clock distribution from PLLs beyond the two multipurpose PLLs directly adjacent to the block.

Figure 1–50 and Figure 1–51 show the detection mechanism example for a successful and unsuccessful receiver detection scenarios respectively. The `tx_forceelecidle` port must be asserted at least 10 parallel clock cycles prior to assertion of `tx_detectrxloop` port to ensure the transmitter buffer is properly tri-stated. Detection completion is indicated by `pipephydonestatus` assertion, with detection successful indicated by 3'b011 on `pipestatus[2..0]` port, or detection unsuccessful by 3'b000 on `pipestatus[2..0]` port.

Figure 1–50. Example of Successful Receiver Detect Operation

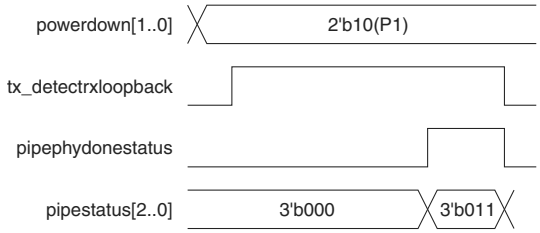
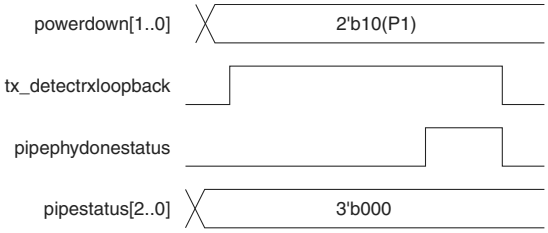


Figure 1–51. Example of Unsuccessful Receiver Detect Operation

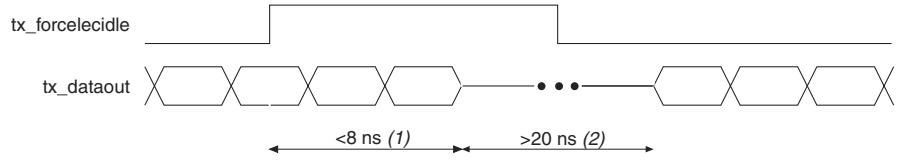


Electrical Idle Control

The Cyclone IV GX transceivers support transmitter buffer in electrical idle state using the `tx_forceelecidle` port. During electrical idle, the transmitter buffer differential and common mode output voltage levels are compliant to the PCIe Base Specification 2.0 for Gen1 signaling rate.

Figure 1–52 shows the relationship between assertion of the `tx_forceelecidle` port and the transmitter buffer output on the `tx_dataout` port.

Figure 1–52. Transmitter Buffer Electrical Idle State



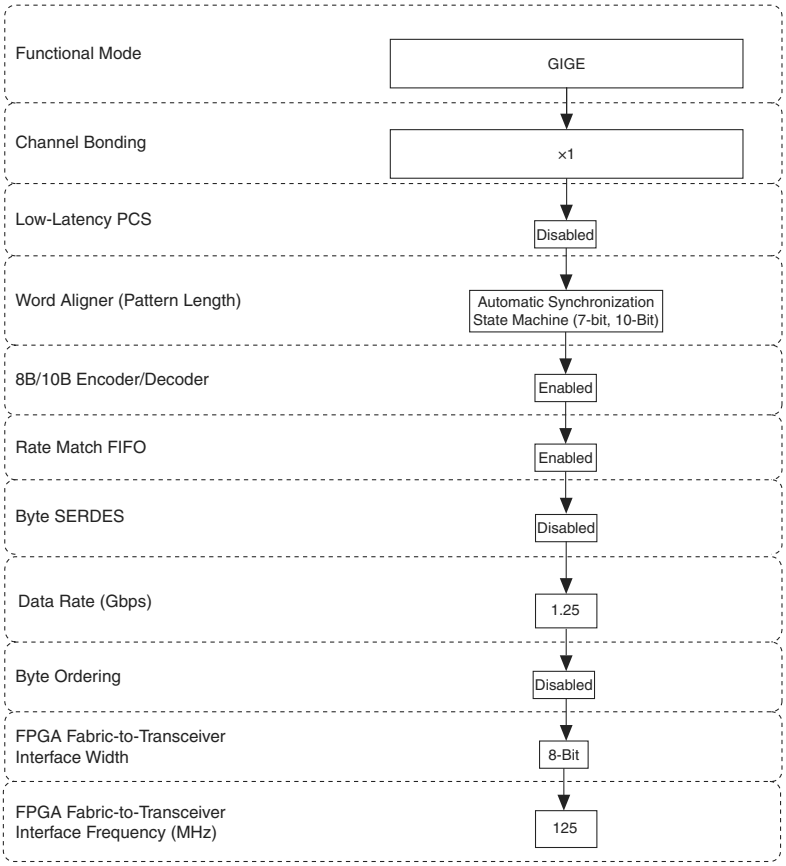
Notes to Figure 1–52:

(1) The protocol requires the transmitter buffer to transition to a valid electrical idle after sending an electrical idle ordered set within 8 ns.

(2) The protocol requires transmitter buffer to stay in electrical idle for a minimum of 20 ns for Gen1 signaling rate.

Figure 1–56 shows the transceiver configuration in GIGE mode.

Figure 1–56. Transceiver Configuration in GIGE Mode



When configured in GIGE mode, three encoded comma (/K28.5/) code groups are transmitted automatically after deassertion of `tx_digitalreset` and before transmitting user data on the `tx_datain` port. This could affect the synchronization state machine behavior at the receiver.

Depending on when you start transmitting the synchronization sequence, there could be an even or odd number of encoded data (/Dx.y/) code groups transmitted between the last of the three automatically sent /K28.5/ code groups and the first /K28.5/ code group of the synchronization sequence. If there is an even number of /Dx.y/ code groups received between these two /K28.5/ code groups, the first /K28.5/ code group of the synchronization sequence begins at an odd code group boundary. An IEEE802.3-compliant GIGE synchronization state machine treats this as an error condition and goes into the Loss-of-Sync state.

Table 1–27. Receiver Ports in ALTGX Megafunction for Cyclone IV GX (Part 3 of 3)

Block	Port Name	Input/ Output	Clock Domain	Description
RX PCS	rx_coreclk	Output	Clock signal	Optional read clock port for the RX phase compensation FIFO.
	rx_phase_comp_fifo_error	Output	Synchronous to `tx_clkout` (non-bonded modes) or `coreclkout` (bonded modes)	RX phase compensation FIFO full or empty indicator. ■ A high level indicates FIFO is either full or empty.
	rx_bitslipboundaryselectout	Output	Asynchronous signal.	Indicate the number of bits slipped in the word aligner configured in manual alignment mode. ■ Values range from 0 to 9.
RX PMA	rx_datain	Input	N/A	Receiver serial data input port.
	rx_freqlocked	Output	Asynchronous signal	Receiver CDR lock state indicator ■ A high level indicates the CDR is in LTD state. ■ A low level indicates the CDR is in LTR state.
	rx_locktodata	Input	Asynchronous signal	Receiver CDR LTD state control signal ■ A high level forces the CDR to LTD state ■ When deasserted, the receiver CDR lock state depends on the `rx_locktorefclk` signal level.
	rx_locktorefclk	Input	Asynchronous signal	Receiver CDR LTR state control signal. ■ The `rx_locktorefclk` and `rx_locktodata` signals control whether the receiver CDR states as follows: [`rx_locktodata:rx_locktorefclk`] ■ 2'b00—receiver CDR is in automatic lock mode ■ 2b'01—receiver CDR is in manual lock mode (LTR state) ■ 2b'1x—receiver CDR is in manual lock mode (LTD state)
	rx_signaldetect	Output	Asynchronous signal	Signal threshold detect indicator. ■ Available in Basic mode when 8B/10B encoder/decoder is used, and in PIPE mode. ■ A high level indicates that the signal present at the receiver input buffer is above the programmed signal detection threshold value.
	rx_recovclkout	Output	Clock signal	CDR low-speed recovered clock ■ Only available in the GIGE mode for applications such as Synchronous Ethernet.

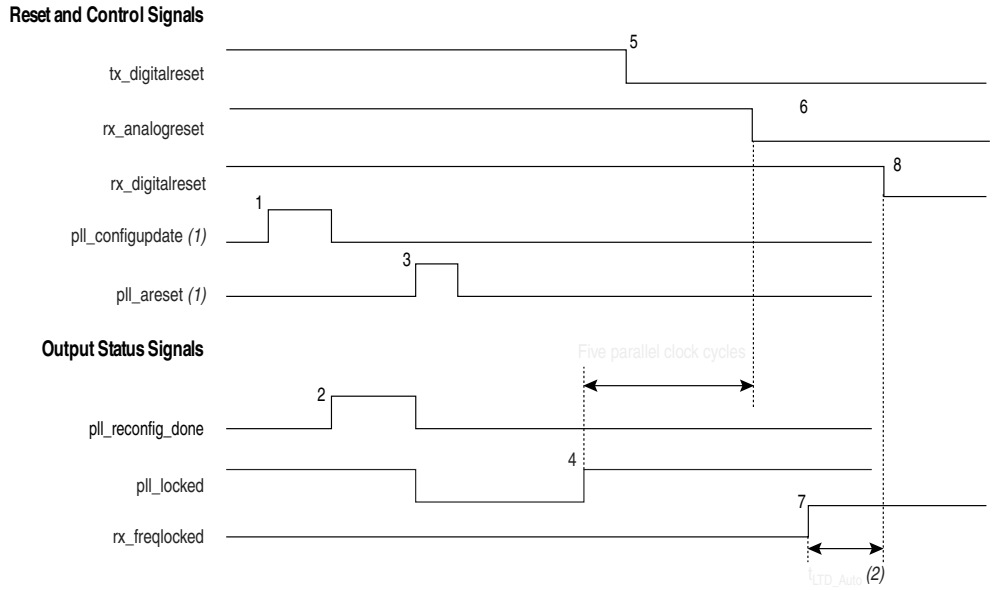
Dynamic Reconfiguration Reset Sequences

When using dynamic reconfiguration in data rate divisions in PLL reconfiguration or channel reconfiguration mode, use the following reset sequences.

Reset Sequence in PLL Reconfiguration Mode

Use the example reset sequence shown in Figure 2–11 when you use the PLL dynamic reconfiguration controller to change the data rate of the transceiver channel. In this example, PLL dynamic reconfiguration is used to dynamically reconfigure the data rate of the transceiver channel configured in Basic ×1 mode with the receiver CDR in automatic lock mode.

Figure 2–11. Reset Sequence When Using the PLL Dynamic Reconfiguration Controller to Change the Data Rate of the Transceiver Channel



Notes to Figure 2–11:

(1) The `pll_configupdate` and `pll_areset` signals are driven by the ALTPLL_RECONFIG megafunction. For more information, refer to *AN 609: Implementing Dynamic Reconfiguration in Cyclone IV GX Devices* and the *Cyclone IV Dynamic Reconfiguration* chapter.

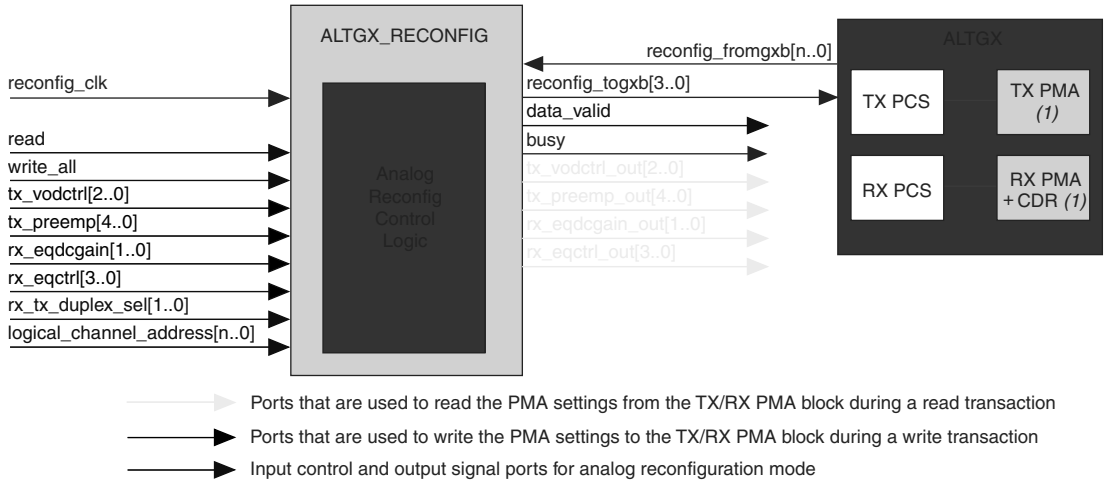
(2) For t_{LTD_Auto} duration, refer to the *Cyclone IV Device Datasheet* chapter.

As shown in Figure 2–11, perform the following reset procedure when using the PLL dynamic reconfiguration controller to change the configuration of the PLLs in the transmitter channel:

1. Assert the `tx_digitalreset`, `rx_analogreset`, and `rx_digitalreset` signals. The `pll_configupdate` signal is asserted (marker 1) by the ALTPLL_RECONFIG megafunction after the final data bit is sent out. The `pll_reconfig_done` signal is asserted (marker 2) to inform the ALTPLL_RECONFIG megafunction that the scan chain process is completed. The ALTPLL_RECONFIG megafunction then asserts the `pll_areset` signal (marker 3) to reset the transceiver PLL.

Figure 3–9 shows the connection for PMA reconfiguration mode.

Figure 3–9. ALTGX and ALTGX_RECONFIG Connection for PMA Reconfiguration Mode



Note to Figure 3–9:

(1) This block can be reconfigured in PMA reconfiguration mode.

Transceiver Channel Reconfiguration Mode

You can dynamically reconfigure the transceiver channel from an existing functional mode to a different functional mode by selecting the **Channel Reconfiguration** option in ALTGX and ALTGX_RECONFIG MegaWizards. The blocks that are reconfigured by channel reconfiguration mode are the PCS and RX PMA blocks of a transceiver channel.

For more information about reconfiguring the RX PMA blocks of the transceiver channel using channel reconfiguration mode, you can refer to "Data Rate Reconfiguration Mode Using RX Local Divider" on page 3–26.

In channel reconfiguration, only a write transaction can occur; no read transactions are allowed. You can optionally choose to trigger `write_all` once by selecting the continuous write operation in the ALTGX_RECONFIG MegaWizard Plug-In Manager. The Quartus II software then continuously writes all the words required for reconfiguration.

For channel reconfiguration, **.mif** files are required to dynamically reconfigure the transceivers channels in channel reconfiguration modes. The **.mif** carries the reconfiguration information that will be used to reconfigure the transceivers channel dynamically on-the-fly. The **.mif** contents is generated automatically when you select the **Generate GXB Reconfig MIF** option in the Quartus II software setting. For different **.mif** settings, you need to later reconfigure and recompile the ALTGX MegaWizard to generate the **.mif** based on the required reconfiguration settings.

The dynamic reconfiguration controller can optionally perform a continuos write operation or a regular write operation of the **.mif** contents in terms of word size (16-bit data) to the transceivers channel that is selected for reconfiguration.

Table 3–4 describes the tx_datainfull[21..0] FPGA fabric-transceiver channel interface signals.

Table 3–4. tx_datainfull[21..0] FPGA Fabric-Transceiver Channel Interface Signal Descriptions (1)

FPGA Fabric-Transceiver Channel Interface Description	Transmit Signal Description (Based on Cyclone IV GX Supported FPGA Fabric-Transceiver Channel Interface Widths)
8-bit FPGA fabric-Transceiver Channel Interface	tx_datainfull[7:0]: 8-bit data (tx_datain)
	The following signals are used only in 8B/10B modes:
	tx_datainfull[8]: Control bit (tx_ctrlenable)
	tx_datainfull[9] Transmitter force disparity Compliance (PCI Express [PIPE]) (tx_forcedisp) in all modes except PCI Express (PIPE) functional mode. For PCI Express (PIPE) functional mode, (tx_forcedispcompliance) is used.
	■ For non-PIPE: tx_datainfull[10]: Forced disparity value (tx_dispval) ■ For PCIe: tx_datainfull[10]: Forced electrical idle (tx_forceelecidle)
10-bit FPGA fabric-Transceiver Channel Interface	tx_datainfull[9:0]: 10-bit data (tx_datain)
16-bit FPGA fabric-Transceiver Channel Interface with PCS-PMA set to 8/10 bits	Two 8-bit Data (tx_datain) tx_datainfull[7:0] - tx_datain (LSByte) and tx_datainfull[18:11] - tx_datain (MSByte)
	The following signals are used only in 8B/10B modes:
	tx_datainfull[8] - tx_ctrlenable (LSB) and tx_datainfull[19] - tx_ctrlenable (MSB)
	Force Disparity Enable ■ For non-PIPE: tx_datainfull[9] - tx_forcedisp (LSB) and tx_datainfull[20] - tx_forcedisp (MSB) ■ For PCIe: tx_datainfull[9] - tx_forcedispcompliance and tx_datainfull[20] - 0
	Force Disparity Value ■ For non-PIPE: tx_datainfull[10] - tx_dispval (LSB) and tx_datainfull[21] - tx_dispval (MSB) ■ For PCIe: tx_datainfull[10] - tx_forceelecidle and tx_datainfull[21] - tx_forceelecidle
20-bit FPGA fabric-Transceiver Channel Interface with PCS-PMA set to 10 bits	Two 10-bit Data (tx_datain) tx_datainfull[9:0] - tx_datain (LSByte) and tx_datainfull[20:11] - tx_datain (MSByte)

Note to Table 3–4:

(1) For all transceiver-related ports, refer to the "Transceiver Port Lists" section in the *Cyclone IV GX Transceiver Architecture* chapter.

Table 1–25. PLL Specifications for Cyclone IV Devices (1), (2) (Part 2 of 2)

Symbol	Parameter	Min	Typ	Max	Unit
t_{DLOCK}	Time required to lock dynamically (after switchover, reconfiguring any non-post-scale counters/delays or areset is deasserted)	—	—	1	ms
$t_{OUTJITTER\_PERIOD\_DEDCLK}$ (6)	Dedicated clock output period jitter $F_{OUT} \geq 100$ MHz	—	—	300	ps
	$F_{OUT} < 100$ MHz	—	—	30	mUI
$t_{OUTJITTER\_CCJ\_DEDCLK}$ (6)	Dedicated clock output cycle-to-cycle jitter $F_{OUT} \geq 100$ MHz	—	—	300	ps
	$F_{OUT} < 100$ MHz	—	—	30	mUI
$t_{OUTJITTER\_PERIOD\_IO}$ (6)	Regular I/O period jitter $F_{OUT} \geq 100$ MHz	—	—	650	ps
	$F_{OUT} < 100$ MHz	—	—	75	mUI
$t_{OUTJITTER\_CCJ\_IO}$ (6)	Regular I/O cycle-to-cycle jitter $F_{OUT} \geq 100$ MHz	—	—	650	ps
	$F_{OUT} < 100$ MHz	—	—	75	mUI
t_{PLL_PSERR}	Accuracy of PLL phase shift	—	—	±50	ps
t_{ARESET}	Minimum pulse width on areset signal.	10	—	—	ns
$t_{CONFIGPLL}$	Time required to reconfigure scan chains for PLLs	—	3.5 (7)	—	SCANCLK cycles
$f_{SCANCLK}$	scanclk frequency	—	—	100	MHz
$t_{CASC\_OUTJITTER\_PERIOD\_DEDCLK}$ (8), (9)	Period jitter for dedicated clock output in cascaded PLLs ($F_{OUT} \geq 100$ MHz)	—	—	425	ps
	Period jitter for dedicated clock output in cascaded PLLs ($F_{OUT} < 100$ MHz)	—	—	42.5	mUI

Notes to Table 1–25:

(1) This table is applicable for general purpose PLLs and multipurpose PLLs.

(2) You must connect V_{CCD_PLL} to V_{CCINT} through the decoupling capacitor and ferrite bead.

(3) This parameter is limited in the Quartus II software by the I/O maximum frequency. The maximum I/O frequency is different for each I/O standard.

(4) The V_{CO} frequency reported by the Quartus II software in the PLL Summary section of the compilation report takes into consideration the V_{CO} post-scale counter K value. Therefore, if the counter K has a value of 2, the frequency reported can be lower than the f_{VCO} specification.

(5) A high input jitter directly affects the PLL output jitter. To have low PLL output clock jitter, you must provide a clean clock source that is less than 200 ps.

(6) Peak-to-peak jitter with a probability level of 10^{-12} (14 sigma, 99.99999999974404% confidence level). The output jitter specification applies to the intrinsic jitter of the PLL when an input jitter of 30 ps is applied.

(7) With 100-MHz scanclk frequency.

(8) The cascaded PLLs specification is applicable only with the following conditions:

- Upstream PLL—0.59 MHz ≤ Upstream PLL bandwidth < 1 MHz
- Downstream PLL—Downstream PLL bandwidth > 2 MHz

(9) PLL cascading is not supported for transceiver applications.