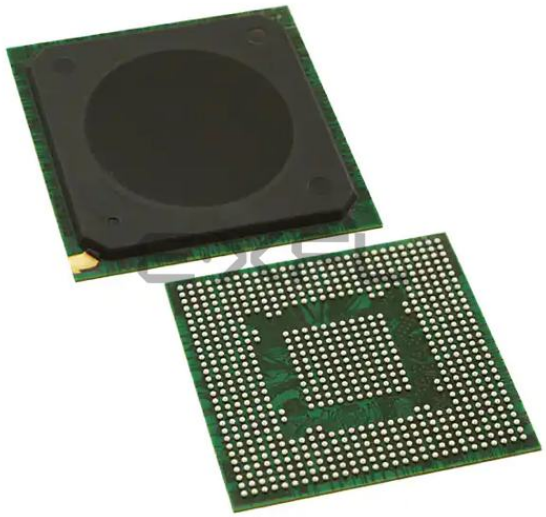

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Understanding Embedded - Microprocessors

Embedded microprocessors are specialized computing chips designed to perform specific tasks within an embedded system. Unlike general-purpose microprocessors found in personal computers, embedded microprocessors are tailored for dedicated functions within larger systems, offering optimized performance, efficiency, and reliability. These microprocessors are integral to the operation of countless electronic devices, providing the computational power necessary for controlling processes, handling data, and managing communications.

Applications of Embedded - Microprocessors

Embedded microprocessors are utilized across a broad spectrum of applications, making them indispensable in

Details	
Product Status	Obsolete
Core Processor	PowerPC e300c4s
Number of Cores/Bus Width	1 Core, 32-Bit
Speed	533MHz
Co-Processors/DSP	Security; SEC 3.0
RAM Controllers	DDR, DDR2
Graphics Acceleration	No
Display & Interface Controllers	-
Ethernet	10/100/1000Mbps (2)
SATA	SATA 3Gbps (2)
USB	USB 2.0 + PHY (1)
Voltage - I/O	1.8V, 2.5V, 3.3V
Operating Temperature	0°C ~ 125°C (TA)
Security Features	Cryptography, Random Number Generator
Package / Case	689-BBGA Exposed Pad
Supplier Device Package	689-TEPBGA II (31x31)
Purchase URL	https://www.e-xfl.com/pro/item?MUrl=&PartUrl=mpc8377evrajf

controller, dual I^2C controllers, a 4-channel DMA controller, an enhanced secured digital host controller, and a general-purpose I/O port. This figure shows the block diagram of the chip.

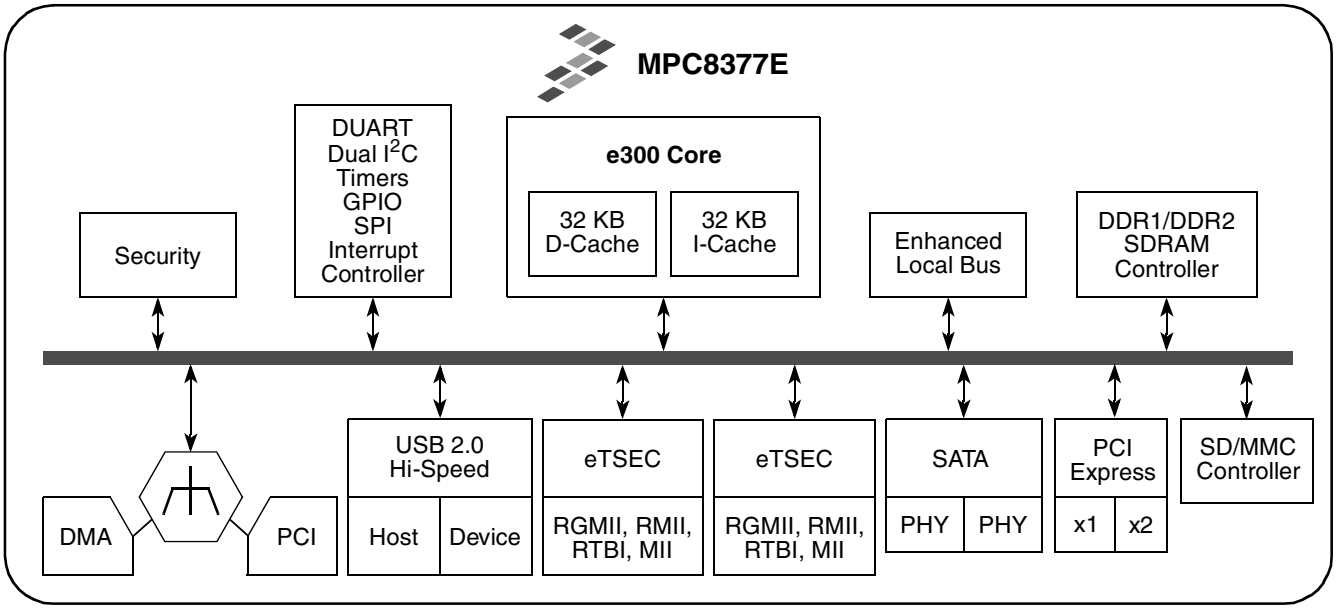

Figure 1. MPC8377E Block Diagram and Features

The following features are supported in the chip:

- e300c4s core built on Power Architecture® technology with 32 KB instruction cache and 32 KB data cache, a floating point unit, and two integer units
- DDR1/DDR2 memory controller supporting a 32/64-bit interface
- Peripheral interfaces, such as a 32-bit PCI interface with up to 66-MHz operation
- 32-bit local bus interface running up to 133-MHz
- USB 2.0 (full/high speed) support
- Power management controller for low-power consumption
- High degree of software compatibility with previous-generation PowerQUICC processor-based designs for backward compatibility and easier software migration
- Optional security engine provides acceleration for control and data plane security protocols

The optional security engine (SEC 3.0) is noted with the extension “E” at the end. It allows CPU-intensive cryptographic operations to be offloaded from the main CPU core. The security-processing accelerator provides hardware acceleration for the DES, 3DES, AES, SHA-1, and MD-5 algorithms.

There are two I^2C controllers. These synchronous, multi-master buses can be connected to additional devices for expansion and system development.

The DUART supports full-duplex operation and is compatible with the PC16450 and PC16550 programming models. 16-byte FIFOs are supported for both the transmitter and the receiver.

The main component of the enhanced local bus controller (eLBC) is its memory controller, which provides a seamless interface to many types of memory devices and peripherals. The memory controller is responsible for controlling eight memory banks shared by a NAND Flash control machine (FCM), a general-purpose chip-select machine (GPCM), and up to three user-programmable machines (UPMs). As such, it supports a minimal glue logic interface to SRAM, EPROM, NOR Flash EPROM, NAND Flash, EPROM, burstable RAM, regular DRAM devices, extended data output DRAM devices, and other peripherals. The eLBC external address latch enable (LALE) signal allows multiplexing of addresses with data signals to reduce the device pin count.

The enhanced local bus controller also includes a number of data checking and protection features, such as data parity generation and checking, write protection, and a bus monitor to ensure that each bus cycle is terminated within a user-specified period. The local bus can operate at up to 133 MHz.

The system timers include the following features: periodic interrupt timer, real time clock, software watchdog timer, and two general-purpose timer blocks.

1.8 Security Engine

The optional security engine is optimized to handle all the algorithms associated with IPSec, IEEE 802.11i, and iSCSI. The security engine contains one crypto-channel, a controller, and a set of crypto execution units (EUs). The execution units are as follows:

- Data encryption standard execution unit (DEU), supporting DES and 3DES
- Advanced encryption standard unit (AESU), supporting AES
- Message digest execution unit (MDEU), supporting MD5, SHA1, SHA-256, and HMAC with any algorithm
- One crypto-channel supporting multi-command descriptor chains

1.9 PCI Controller

The PCI controller includes the following features:

- *PCI Specification Revision 2.3* compatible
- Single 32-bit data PCI interface operates at up to 66 MHz
- PCI 3.3-V compatible (not 5-V compatible)
- Support for host and agent modes
- On-chip arbitration, supporting 5 external masters on PCI
- Selectable hardware-enforced coherency

Table 6. Typical I/O Power Dissipation (continued)

Interface	Parameter	GV_{DD} (1.8 V)	GV_{DD}/LBV_{DD} (2.5 V)	OV_{DD} (3.3 V)	LV_{DD} (3.3 V)	LV_{DD} (2.5 V)	$L[1,2]\_nV_{DD}$ (1.0 V)	Unit	Comments
PCI I/O Load = 30 pf	33 MHz, 32-bit	—	—	0.04	—	—	—	W	—
	66 MHz, 32-bit	—	—	0.07	—	—	—	W	
Local Bus I/O Load = 25 pf	167 MHz, 32-bit	0.09	0.17	0.29	—	—	—	W	—
	133 MHz, 32-bit	0.07	0.14	0.24	—	—	—	W	
	83 MHz, 32-bit	0.05	0.09	0.15	—	—	—	W	
	66 MHz, 32-bit	0.04	0.07	0.13	—	—	—	W	
	50 MHz, 32-bit	0.03	0.06	0.1	—	—	—	W	
eTSEC I/O Load = 25 pf	MII or RMII	—	—	—	0.02	—	—	W	Multiply by number of interfaces used.
	RGMII or RTBI	—	—	—	—	0.05	—	W	—
USB (60MHz Clock)	12 Mbps	—	—	0.01	—	—	—	W	—
	480 Mbps	—	—	0.2	—	—	—	W	
SerDes	per lane	—	—		—	—	0.029	W	—
Other I/O	—	—	—	0.01	—	—	—	W	—

Note: The values given are for typical, and not worst case, switching.

4 Clock Input Timing

This section provides the clock input DC and AC electrical characteristics for the chip. Note that the PCI_CLK/PCI_SYNC_IN signal or CLKIN signal is used as the PCI input clock depending on whether the device is configured as a host or agent device. CLKIN is used when the device is in host mode.

6.2.2 DDR1 and DDR2 SDRAM Output AC Timing Specifications

This table shows the DDR1 and DDR2 SDRAM output AC timing specifications.

Table 21. DDR1 and DDR2 SDRAM Output AC Timing Specifications

Parameter	Symbol[1]	Min	Max	Unit	Note
MCK*n* cycle time, MCK*n*/$\overline{\text{MCK}n}$ crossing	t_{MCK}	5	10	ns	2
ADDR/CMD output setup with respect to MCK 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHAS}	 1.95 2.40 3.15 4.20	 — — — —	ns	3, 7
ADDR/CMD output hold with respect to MCK 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHAX}	 1.95 2.40 3.15 4.20	 — — — —	ns	3, 7
$\overline{\text{MCS}n}$ output setup with respect to MCK 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHCS}	 1.95 2.40 3.15 4.20	 — — — —	ns	3
$\overline{\text{MCS}n}$ output hold with respect to MCK 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHCX}	 1.95 2.40 3.15 4.20	 — — — —	ns	3
MCK to MDQS skew	t_{DDKHMH}	–0.6	0.6	ns	4, 8
MDQ//MDM output setup with respect to MDQS 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHDS}, t_{DDKLDS}	 550 800 1100 1200	 — — — —	ps	5, 8
MDQ//MDM output hold with respect to MDQS 400 MHz data rate 333 MHz data rate 266 MHz data rate 200 MHz data rate	t_{DDKHDX}, t_{DDKLDX}	 700 800 1100 1200	 — — — —	ps	5, 8
MDQS preamble start	t_{DDKHMP}	$-0.5 \times t_{MCK} - 0.6$	$-0.5 \times t_{MCK} + 0.6$	ns	6, 8

This table describes the general timing parameters of the local bus interface of the device when in PLL bypass mode.

Table 40. Local Bus General Timing Parameters—PLL Bypass Mode

Parameter	Symbol[1]	Min	Max	Unit	Note
Local bus cycle time	t_{LBK}	15	—	ns	2
Input setup to local bus clock	t_{LBIVKH}	7.0	—	ns	3, 4
Input hold from local bus clock	t_{LBIXKH}	1.0	—	ns	3, 4
LALE output fall to LAD output transition (LATCH hold time)	$t_{LBOTOT1}$	1.5	—	ns	5
LALE output fall to LAD output transition (LATCH hold time)	$t_{LBOTOT2}$	3.0	—	ns	6
LALE output fall to LAD output transition (LATCH hold time)	$t_{LBOTOT3}$	2.5	—	ns	7
Local bus clock to LALE rise	t_{LBKHLR}	—	4.5	ns	—
Local bus clock to output valid	t_{LBKHOV}	—	3.0	ns	3
Local bus clock to output high impedance for LAD/LDP	t_{LBKHOZ}	—	4.0	ns	3, 8

Notes:

1. The symbols used for timing specifications herein follow the pattern of $t_{\text{(First two letters of functional block)(signal)(state)(reference)(state)}}$ for inputs and $t_{\text{(First two letters of functional block)(reference)(state)(signal)(state)}}$ for outputs. For example, $t_{LBIXKH1}$ symbolizes local bus timing (LB) for the input (I) to go invalid (X) with respect to the time the t_{LBK} clock reference (K) goes high (H), in this case for clock one(1). Also, t_{LBKHOX} symbolizes local bus timing (LB) for the t_{LBK} clock reference (K) to go high (H), with respect to the output (O) going invalid (X) or output hold time.
2. All timings are in reference to falling edge of LCLK0 (for all outputs and for $\overline{\text{LGTA}}$ and LUPWAIT inputs) or rising edge of LCLK0 (for all other inputs).
3. All signals are measured from $LBV_{DD}/2$ of the rising/falling edge of LCLK0 to $0.4 \times LBV_{DD}$ of the signal in question for 3.3-V signaling levels.
4. Input timings are measured at the pin.
5. $t_{LBOTOT1}$ should be used when LBCR[AHD] is set and the load on LALE output pin is at least 10pF less than the load on LAD output pins.
6. $t_{LBOTOT2}$ should be used when LBCR[AHD] is not set and the load on LALE output pin is at least 10pF less than the load on LAD output pins.
7. $t_{LBOTOT3}$ should be used when LBCR[AHD] is not set and the load on LALE output pin equals to the load on LAD output pins.
8. For purposes of active/float timing measurements, the Hi-Z or off state is defined to be when the total current delivered through the component pin is less than or equal to the leakage current specification.

This figure provides the AC test load for the local bus.

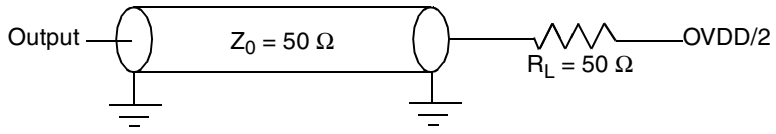

Figure 19. Local Bus AC Test Load

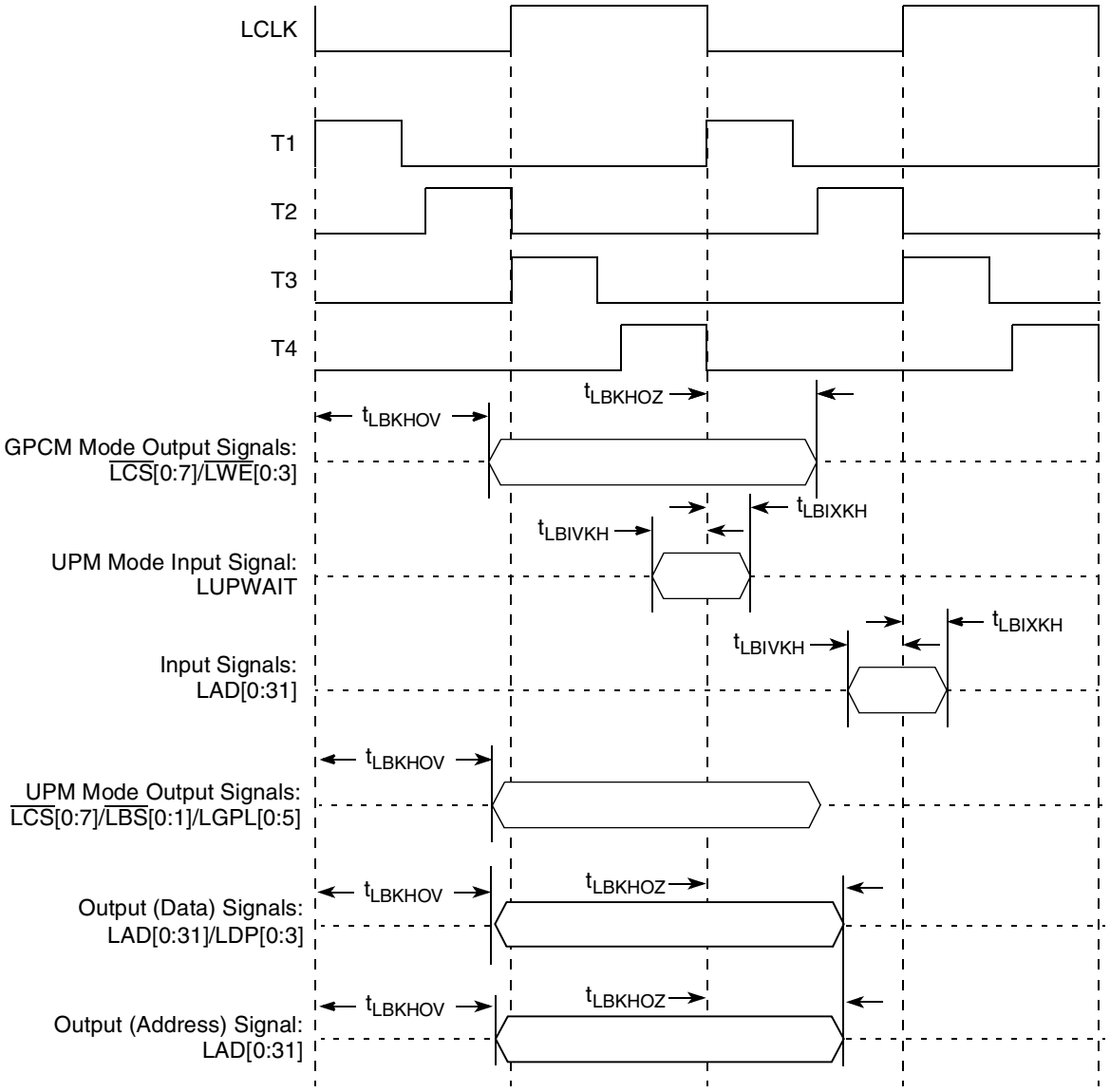

Figure 25. Local Bus Signals, GPCM/UPM Signals for LCRR[CLKDIV] = 4 (PLL Bypass Mode)

11 Enhanced Secure Digital Host Controller (eSDHC)

This section describes the DC and AC electrical specifications for the eSDHC (SD/MMC) interface of the chip.

The eSDHC controller always uses the falling edge of the SD_CLK in order to drive the SD_DAT[0:3]/CMD as outputs and sample the SD_DAT[0:3] as inputs. This behavior is true for both full- and high-speed modes.

Note that this is a non-standard implementation, as the SD card specification assumes that in high-speed mode, data is driven at the rising edge of the clock.

$$t_{CLK\_DELAY} + t_{IH} - t_{SFSKHOX} < t_{SFSCKL} + t_{DATA\_DELAY} \quad \text{Eqn. 5}$$

This means that clock can be delayed versus data up to 15 ns (external delay line) in ideal case of $t_{SFSCLKL}$ = 20 ns:

$t_{CLK\_DELAY} + 5 - 0 < 20 + t_{DATA\_DELAY}$

$t_{CLK\_DELAY} < 15 + t_{DATA\_DELAY}$

11.2.1.3 Full-Speed Write Combined Formula

The following equation is the combined formula to calculate the allowed skew range between the SD_CLK and SD_DAT/CMD signals on the PCB.

$$t_{CLK\_DELAY} + t_{IH} - t_{SFSKHOX} < t_{SFSCKL} + t_{DATA\_DELAY} < t_{SFSCK} + t_{CLK\_DELAY} - t_{ISU} - t_{SFSKHOV} \quad \text{Eqn. 6}$$

11.2.2 Full-Speed Input Path (Read)

This figure provides the data and command input timing diagram.

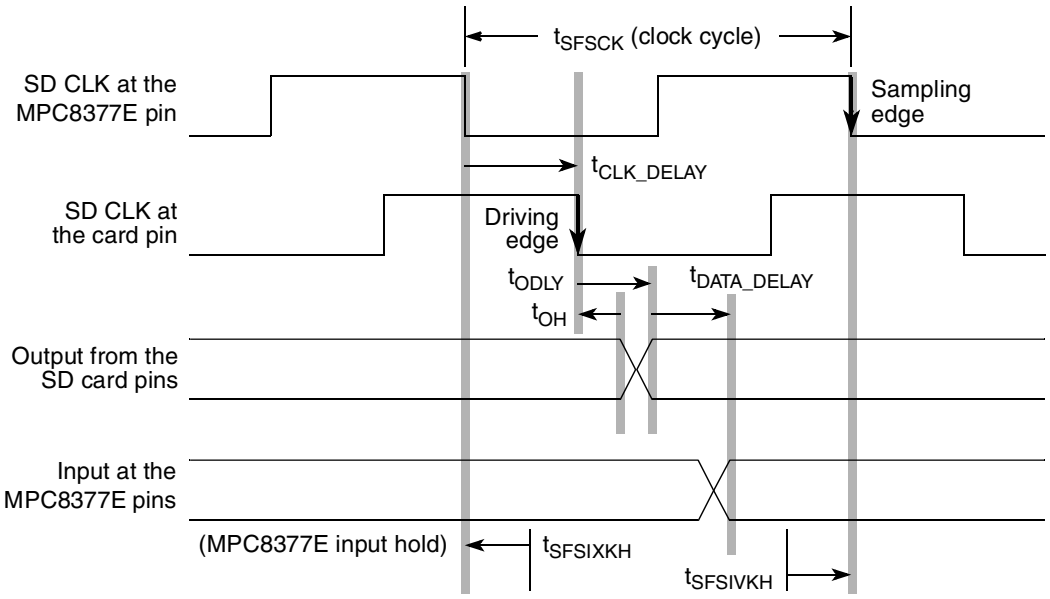

Figure 28. Full Speed Input Path

11.2.2.1 Full-Speed Read Meeting Setup (Maximum Delay)

The following equations show how to calculate the allowed combined propagation delay range of the SD_CLK and SD_DAT/CMD signals on the PCB.

$$t_{CLK\_DELAY} + t_{DATA\_DELAY} + t_{ODLY} + t_{SFSIVKH} < t_{SFSCK} \quad \text{Eqn. 7}$$

$$t_{CLK\_DELAY} + t_{DATA\_DELAY} < t_{SFSCK} - t_{ODLY} - t_{SFSIVKH} - t_{INT\_CLK\_DLY} \quad \text{Eqn. 8}$$

Table 52. Differential Transmitter (Tx) Output Specifications (continued)

Parameter	Conditions	Symbol	Min	Typical	Max	Units	Note
Absolute delta of DC common mode between D+ and D–	$\lvert V_{TX\text{-}CM\text{-}DC\text{-}D+} - V_{TX\text{-}CM\text{-}DC\text{-}D-} \rvert \leq 25$ mV $V_{TX\text{-}CM\text{-}DC\text{-}D+} = DC_{(avg)}$ of $\lvert V_{TX\text{-}D+} \rvert$ $V_{TX\text{-}CM\text{-}DC\text{-}D-} = DC_{(avg)}$ of $\lvert V_{TX\text{-}D-} \rvert$	$V_{TX\text{-}CM\text{-}DC\text{-}LINE\text{-}DELTA}$	0	—	25	mV	2
Electrical idle differential peak output voltage	$V_{PEEIDPTX} = \lvert V_{TX\text{-}IDLE\text{-}D+} - V_{TX\text{-}IDLE\text{-}D-} \rvert \leq 20$ mV	$V_{TX\text{-}IDLE\text{-}DIFFp}$	0	—	20	mV	2
Amount of voltage change allowed during receiver detection	The total amount of voltage change that a transmitter can apply to sense whether a low impedance receiver is present.	$V_{TX\text{-}RCV\text{-}DETECT}$	—	$XPADV_{DD}/2$	600	mV	6
Tx DC common mode voltage	The allowed DC common mode voltage under any conditions.	$V_{TX\text{-}DC\text{-}CM}$	0	$XPADV_{DD}/2$	—	V	6
Tx short circuit current limit	The total current the transmitter can provide when shorted to its ground	$I_{TX\text{-}SHORT}$	—	—	90	mA	—
Minimum time spent in electrical idle	Minimum time a transmitter must be in electrical idle. Utilized by the receiver to start looking for an electrical idle exit after successfully receiving an electrical idle ordered set.	$T_{TX\text{-}IDLE\text{-}MIN}$	50	—	—	UI	—
Maximum time to transition to a valid electrical idle after sending an electrical idle ordered set	After sending an electrical idle ordered set, the transmitter must meet all electrical idle specifications within this time. This is considered a debounce time for the transmitter to meet electrical idle after transitioning from LO.	$T_{TX\text{-}IDLE\text{-}SET\text{-}TO\text{-}IDLE}$	—	—	20	UI	—
Maximum time to transition to valid Tx specifications after leaving an electrical idle condition	Maximum time to meet all Tx specifications when transitioning from electrical idle to sending differential data. This is considered a debounce time for the Tx to meet all Tx specifications after leaving electrical idle	$T_{TX\text{-}IDLE\text{-}TO\text{-}DIFF\text{-}DATA}$	—	—	20	UI	—
Differential return loss	Measured over 50 MHz to 1.25 GHz.	$RL_{TX\text{-}DIFF}$	12	—	—	dB	4

The eye diagram must be valid for any 250 consecutive UIs.

A recovered Tx UI is calculated over 3500 consecutive unit intervals of sample data. The eye diagram is created using all edges of the 250 consecutive UI in the center of the 3500 UI used for calculating the Tx UI.

NOTE

It is recommended that the recovered Tx UI be calculated using all edges in the 3500 consecutive UI interval with a fit algorithm using a minimization merit function (that is, least squares and median deviation fits).

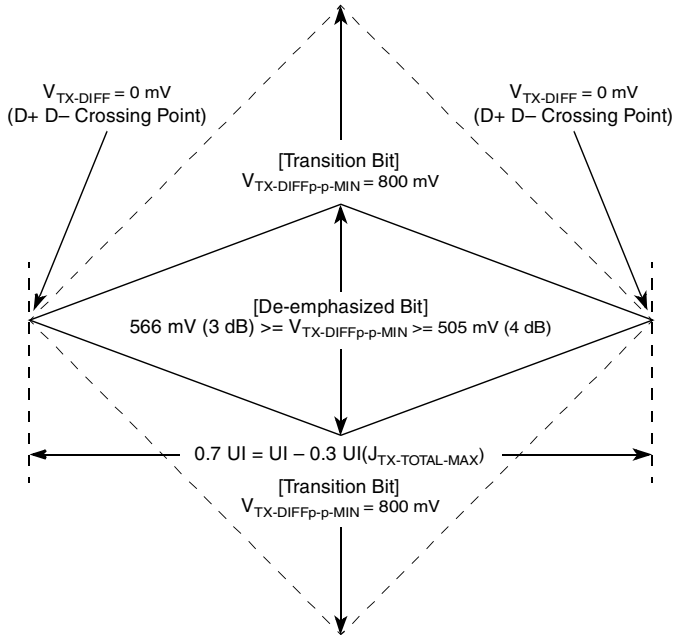

Figure 42. Minimum Transmitter Timing and Voltage Output Compliance Specifications

15.4.3 Differential Receiver (Rx) Input Specifications

This table defines the specifications for the differential input at all receivers. The parameters are specified at the component pins.

Table 53. Differential Receiver (Rx) Input Specifications

Parameter	Comments	Symbol	Min	Typical	Max	Units	Note
Unit interval	Each U_{PERX} is 400 ps ± 300 ppm. U_{PERX} does not account for Spread Spectrum Clock dictated variations.	UI	399.88	400	400.12	ps	1
Differential peak-to-peak output voltage	$V_{PEDPPRX} = 2 \times \lvert V_{RX-D+} - V_{RX-D-} \rvert$	$V_{RX-DIFFp-p}$	0.175	—	1.200	V	2

Table 53. Differential Receiver (Rx) Input Specifications (continued)

Parameter	Comments	Symbol	Min	Typical	Max	Units	Note
Unexpected Electrical Idle Enter Detect Threshold Integration Time	An unexpected electrical idle (Vrx-diffp-p < Vrx-idle-det-diffp-p) must be recognized no longer than Trx-idle-det-diff-entertime to signal an unexpected idle condition.	$T_{RX-IDLE-DET-DIFF-ENTERTIME}$	—	—	10	ms	—
Total Skew	Skew across all lanes on a link. This includes variation in the length of SKP ordered set (e.g. COM and one to five SKP Symbols) at the Rx as well as any delay differences arising from the interconnect itself.	$L_{RX-SKEW}$	—	—	20	ns	—

Notes:
1. No test load is necessarily associated with this value.
2. Specified at the measurement point and measured over any 250 consecutive UIs. The test load in Figure 44 should be used as the Rx device when taking measurements (also refer to the receiver compliance eye diagram shown in Figure 43). If the clocks to the Rx and Tx are not derived from the same reference clock, the Tx UI recovered from 3500 consecutive UI must be used as a reference for the eye diagram.
3. A T_{Rx-EYE} = 0.40 UI provides for a total sum of 0.60 UI deterministic and random jitter budget for the transmitter and interconnect collected any 250 consecutive UIs. The TRx-EYE-MEDIAN-to-MAX-JITTER specification ensures a jitter distribution in which the median and the maximum deviation from the median is less than half of the total. UI jitter budget collected over any 250 consecutive Tx UIs. It should be noted that the median is not the same as the mean. The jitter median describes the point in time where the number of jitter points on either side is approximately equal as opposed to the averaged time value. If the clocks to the Rx and Tx are not derived from the same reference clock, the Tx UI recovered from 3500 consecutive UI must be used as the reference for the eye diagram.
4. The receiver input impedance will result in a differential return loss greater than or equal to 10 dB with the D+ line biased to 300 mV and the D– line biased to –300 mV and a common mode return loss greater than or equal to 6 dB (no bias required) over a frequency range of 50 MHz to 1.25 GHz. This input impedance requirement applies to all valid input levels. The reference impedance for return loss measurements for is 50 Ω to ground for both the D+ and D– line (that is, as measured by a vector network analyzer with 50-Ω probes, see Figure 44). Note that the series capacitors, C_{Tx}, is optional for the return loss measurement.
5. Impedance during all LTSSM states. When transitioning from a fundamental reset to detect (the initial state of the LTSSM) there is a 5 ms transition time before receiver termination values must be met on all unconfigured lanes of a port.
6. The Rx DC common mode impedance that exists when no power is present or fundamental reset is asserted. This helps ensure that the receiver detect circuit does not falsely assume a receiver is powered on when it is not. This term must be measured at 300 mV above the Rx ground.
7. It is recommended that the recovered Tx UI is calculated using all edges in the 3500 consecutive UI interval with a fit algorithm using a minimization merit function. Least squares and median deviation fits have worked well with experimental and simulated data.

15.5 Receiver Compliance Eye Diagrams

The Rx eye diagram in Figure 43 is specified using the passive compliance/test measurement load (see Figure 44) in place of any real PCI Express Rx component. In general, the minimum receiver eye diagram measured with the compliance/test measurement load (see Figure 44) is larger than the minimum receiver eye diagram measured over a range of systems at the input receiver of any real PCI Express component. The degraded eye diagram at the input receiver is due to traces internal to the package as well as silicon parasitic characteristics that cause the real PCI Express component to vary in impedance from the

compliance/test measurement load. The input receiver eye diagram is implementation specific and is not specified. Rx component designer should provide additional margin to adequately compensate for the degraded minimum receiver eye diagram (shown in Figure 43) expected at the input receiver based on an adequate combination of system simulations and the return loss measured looking into the Rx package and silicon. The Rx eye diagram must be aligned in time using the jitter median to locate the center of the eye diagram.

The eye diagram must be valid for any 250 consecutive UIs.

A recovered Tx UI is calculated over 3500 consecutive unit intervals of sample data. The eye diagram is created using all edges of the 250 consecutive UI in the center of the 3500 UI used for calculating the Tx UI.

NOTE

The reference impedance for return loss measurements is 50 Ω to ground for both the D+ and D– line (that is, as measured by a Vector Network Analyzer with 50 Ω probes—see Figure 44). Note that the series capacitors, $C_{PEACCTX}$, are optional for the return loss measurement.

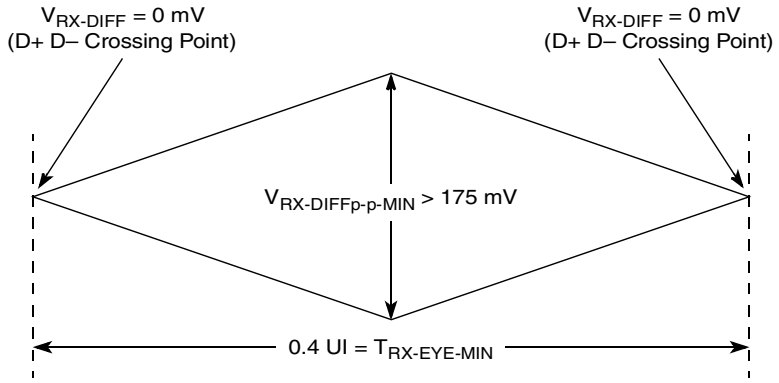

Figure 43. Minimum Receiver Eye Timing and Voltage Compliance Specification

18 GPIO

This section describes the DC and AC electrical specifications for the GPIO of the chip.

18.1 GPIO DC Electrical Characteristics

This table provides the DC electrical characteristics for the device GPIO.

Table 65. GPIO DC Electrical Characteristics

This specification applies when operating at 3.3 V ± 165 mV supply.

Parameter	Condition	Symbol	Min	Max	Unit
Output high voltage	I_{OH} = –6.0 mA	V_{OH}	2.4	—	V
Output low voltage	I_{OL} = 6.0 mA	V_{OL}	—	0.5	V
Output low voltage	I_{OL} = 3.2 mA	V_{OL}	—	0.4	V
Input high voltage	—	V_{IH}	2.0	OV_{DD} + 0.3	V
Input low voltage	—	V_{IL}	–0.3	0.8	V
Input current	0 V ≤ V_{IN} ≤ OV_{DD}	I_{IN}	—	± 30	μA

18.2 GPIO AC Timing Specifications

This table provides the GPIO input and output AC timing specifications.

Table 66. GPIO Input AC Timing Specifications

Parameter	Symbol	Min	Unit
GPIO inputs—minimum pulse width	t_{PIWID}	20	ns

Notes:

1. Input specifications are measured from the 50% level of the signal to the 50% level of the rising edge of SYS_CLKIN. Timings are measured at the pin.
2. GPIO inputs and outputs are asynchronous to any visible clock. GPIO outputs should be synchronized before use by any external synchronous logic. GPIO inputs are required to be valid for at least t_{PIWID} ns to ensure proper operation.

This figure provides the AC test load for the GPIO.

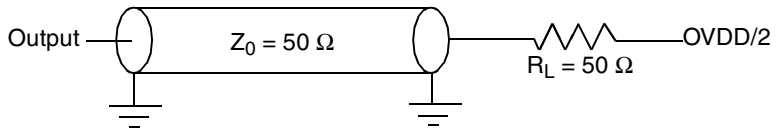

Figure 47. GPIO AC Test Load

19 IPIC

This section describes the DC and AC electrical specifications for the external interrupt pins of the chip.

driver chip manufacturer to verify whether this connection scheme is compatible with a particular clock driver chip.

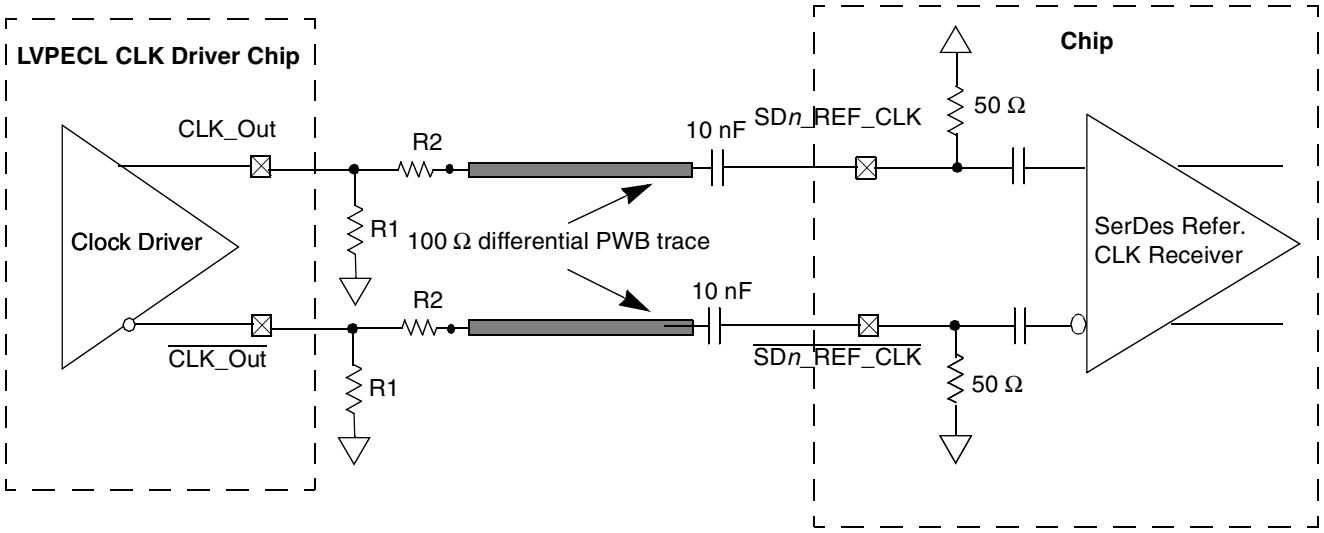

Figure 58. AC-Coupled Differential Connection with LVPECL Clock Driver (Reference Only)

This figure shows the SerDes reference clock connection reference circuits for a single-ended clock driver. It assumes the DC levels of the clock driver are compatible with device SerDes reference clock input's DC requirement.

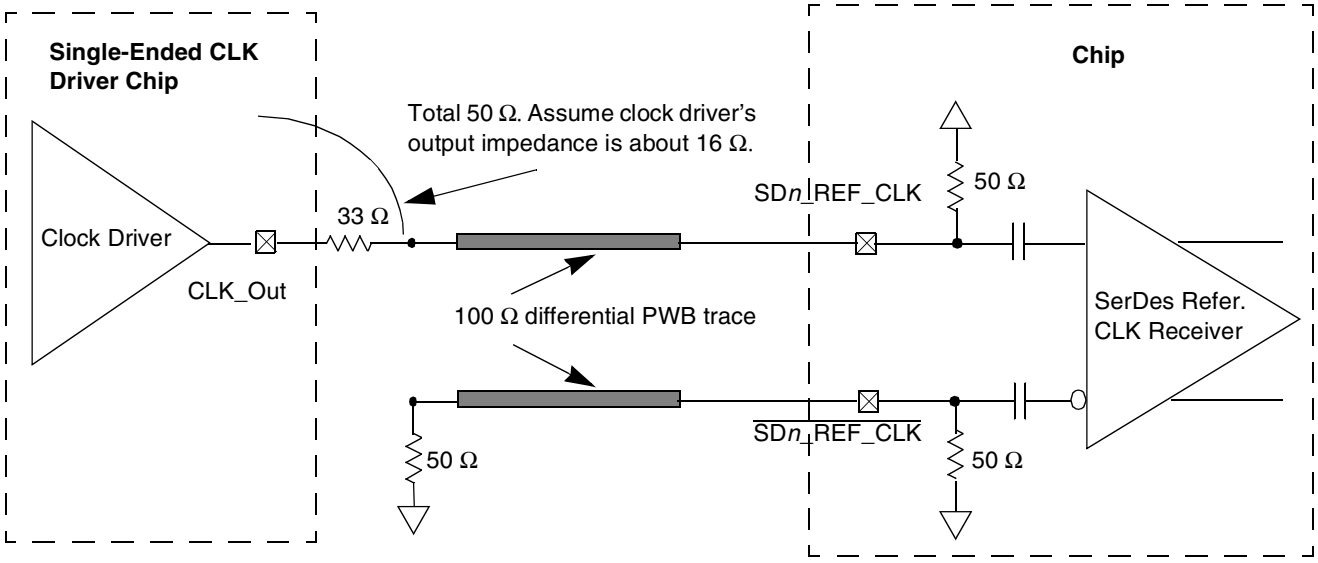

Figure 59. Single-Ended Connection (Reference Only)

21.2.4 AC Requirements for SerDes Reference Clocks

The clock driver selected should provide a high quality reference clock with low phase noise and cycle-to-cycle jitter. Phase noise less than 100 KHz can be tracked by the PLL and data recovery loops and is less of a problem. Phase noise above 15 MHz is filtered by the PLL. The most problematic phase noise

Table 72. TePBGA II Pinout Listing (continued)

Signal	Package Pin Number	Pin Type	Power Supply	Note
UART_RTS_B[2]	L29	O	OVDD	—
Enhanced Local Bus Controller (eLBC) Interface				
LAD0	E24	I/O	LBVDD	—
LAD1	G28	I/O	LBVDD	—
LAD2	H25	I/O	LBVDD	—
LAD3	F26	I/O	LBVDD	—
LAD4	C26	I/O	LBVDD	—
LAD5	J28	I/O	LBVDD	—
LAD6	F21	I/O	LBVDD	—
LAD7	F23	I/O	LBVDD	—
LAD8	E25	I/O	LBVDD	—
LAD9	E26	I/O	LBVDD	—
LAD10	A23	I/O	LBVDD	—
LAD11	F24	I/O	LBVDD	—
LAD12	G24	I/O	LBVDD	—
LAD13	F25	I/O	LBVDD	—
LAD14	H28	I/O	LBVDD	—
LAD15	G25	I/O	LBVDD	—
LA11/LAD16	F27	I/O	LBVDD	—
LA12/LAD17	B21	I/O	LBVDD	—
LA13/LAD18	A25	I/O	LBVDD	—
LA14/LAD19	C28	I/O	LBVDD	—
LA15/LAD20	H24	I/O	LBVDD	—
LA16/LAD21	E23	I/O	LBVDD	—
LA17/LAD22	B28	I/O	LBVDD	—
LA18/LAD23	D28	I/O	LBVDD	—
LA19/LAD24	A27	I/O	LBVDD	—
LA20/LAD25	C25	I/O	LBVDD	—
LA21/LAD26	B27	I/O	LBVDD	—
LA22/LAD27	H27	I/O	LBVDD	—
LA23/LAD28	E21	I/O	LBVDD	—
LA24/LAD29	F20	I/O	LBVDD	—

Table 72. TePBGA II Pinout Listing (continued)

Signal	Package Pin Number	Pin Type	Power Supply	Note
TSEC2_RXD0/GPIO1[16]	AE28	I/O	LVDD2	16
TSEC2_RXD1/GPIO1[15]	AE29	I/O	LVDD2	16
TSEC2_RXD2/GPIO1[14]	AH26	I/O	LVDD2	16
TSEC2_RXD3/GPIO1[13]	AH25	I/O	LVDD2	16
TSEC2_TX_CLK/GPIO2[24]/ TSEC1_TMR_GCLK	AG28	I/O	LVDD2	16
TSEC2_TX_EN/GPIO1[12]/ TSEC1_TMR_ALARM2	AJ26	I/O	LVDD2	16
TSEC2_TX_ER/GPIO1[24]/ TSEC1_TMR_ALARM1	AG26	I/O	LVDD2	16
TSEC2_TXD0/GPIO1[20]	AH28	I/O	LVDD2	16
TSEC2_TXD1/GPIO1[19]/ TSEC1_TMR_PP1	AF27	I/O	LVDD2	16
TSEC2_TXD2/GPIO1[18]/ TSEC1_TMR_PP2	AJ28	I/O	LVDD2	16
TSEC2_TXD3/GPIO1[17]/ TSEC1_TMR_PP3	AF29	I/O	LVDD2	16
GPIO1 Interface				
GPIO1[0]/GTM1_TIN1/ GTM2_TIN2/DREQ0_B	P25	I/O	OVDD	—
GPIO1[1]/GTM1_TGATE1_B/ GTM2_TGATE2_B/DACK0_B	N25	I/O	OVDD	—
GPIO1[2]/GTM1_TOUT1_B/ DDONE0_B	N26	I/O	OVDD	—
GPIO1[3]/GTM1_TIN2/ GTM2_TIN1/DREQ1_B	B9	I/O	OVDD	—
GPIO1[4]/GTM1_TGATE2_B/ GTM2_TGATE1_B/DACK1_B	N29	I/O	OVDD	—
GPIO1[5]/GTM1_TOUT2_B/ GTM2_TOUT1_B/DDONE1_B	M29	I/O	OVDD	—
GPIO1[6]/GTM1_TIN3/ GTM2_TIN4/DREQ2_B	A9	I/O	OVDD	—
GPIO1[7]/GTM1_TGATE3_B/ GTM2_TGATE4_B/DACK2_B	B10	I/O	OVDD	—
GPIO1[8]/GTM1_TOUT3_B/ DDONE2_B	J26	I/O	OVDD	—
GPIO1[9]/GTM1_TIN4/ GTM2_TIN3/DREQ3_B	J24	I/O	OVDD	—

As shown in Figure 64, the primary clock input (frequency) is multiplied up by the system phase-locked loop (PLL) and the clock unit to create the coherent system bus clock (*csb_clk*), the internal clock for the DDR controller (*ddr_clk*), and the internal clock for the local bus interface unit (*lbiu_clk*).

The *csb_clk* frequency is derived from a complex set of factors that can be simplified into the following equation:

$$csb\_clk = \{PCI\_SYNC\_IN \times (1 + CFG\_CLKIN\_DIV)\} \times SPMF \qquad \text{Eqn. 20}$$

In PCI host mode, PCI_SYNC_IN × (1 + CFG_CLKIN_DIV) is the CLKIN frequency.

The *csb_clk* serves as the clock input to the e300 core. A second PLL inside the e300 core multiplies up the *csb_clk* frequency to create the internal clock for the e300 core (*core_clk*). The system and core PLL multipliers are selected by the SPMF and COREPLL fields in the reset configuration word low register (RCWLR) which is loaded at power-on reset or by one of the hard-coded reset options. See Chapter 4, "Reset, Clocking, and Initialization," in the *MPC8379E Reference Manual* for more information on the clock subsystem.

The internal *ddr_clk* frequency is determined by the following equation:

$$ddr\_clk = csb\_clk \times (1 + RCWLR[DDRCM]) \qquad \text{Eqn. 21}$$

Note that *ddr_clk* is not the external memory bus frequency; *ddr_clk* passes through the DDR clock divider (÷2) to create the differential DDR memory bus clock outputs (MCK and $\overline{\text{MCK}}$). However, the data rate is the same frequency as *ddr_clk*.

The internal *lbiu_clk* frequency is determined by the following equation:

$$lbiu\_clk = csb\_clk \times (1 + RCWLR[LBCM]) \qquad \text{Eqn. 22}$$

Note that *lbiu_clk* is not the external local bus frequency; *lbiu_clk* passes through the LBIU clock divider to create the external local bus clock outputs (LCLK[0:2]). The eLBC clock divider ratio is controlled by LCRR[CLKDIV].

Some of the internal units may be required to be shut off or operate at lower frequency than the *csb_clk* frequency. Those units have a default clock ratio that can be configured by a memory mapped register after the device comes out of reset. Table 73 specifies which units have a configurable clock frequency.

Table 73. Configurable Clock Units

Unit	Default Frequency	Options
eTSEC1, eTSEC2	csb_clk/3	Off, *csb_clk, csb_clk/2, csb_clk/3*
eSDHC and I^2C1[1]	csb_clk/3	Off, *csb_clk, csb_clk/2, csb_clk/3*
Security block	csb_clk/3	Off, *csb_clk, csb_clk/2, csb_clk/3*
USB DR	csb_clk/3	Off, *csb_clk, csb_clk/2, csb_clk/3*
PCI and DMA complex	csb_clk	Off, *csb_clk*

Table 79. e300 Core PLL Configuration (continued)

RCWLR[COREPLL]			*core_clk* : *csb_clk* Ratio	VCO Divider [1]
0–1	2–5	6		
01	**0001**	1	1.5:1	4
10	**0001**	1	1.5:1	8
00	**0010**	0	2:1	2
01	**0010**	0	2:1	4
10	**0010**	0	2:1	8
00	**0010**	1	2.5:1	2
01	**0010**	1	2.5:1	4
10	**0010**	1	2.5:1	8
00	**0011**	0	3:1	2
01	**0011**	0	3:1	4
10	**0011**	0	3:1	8
00	**0011**	1	3.5:1	2
01	**0011**	1	3.5:1	4
10	**0011**	1	3.5:1	8
00	**0100**	0	4:1	2
01	**0100**	0	4:1	4
10	**0100**	0	4:1	8

Notes:
1. Core VCO frequency = Core frequency × VCO divider. Note that VCO divider has to be set properly so that the core VCO frequency is in the range of 800–1600 MHz.

23.3 Suggested PLL Configurations

This table shows suggested PLL configurations for different input clocks (LBCM = 0).

Table 80. Example Clock Frequency Combinations

								eLBC [1]			e300 Core [1]				
Ref [1]	**LBCM**	**DDRCM**	**SVCOD**	**SPMF**	**Sys VCO[1,2]**	**CSB[1,3]**	**DDR data rate[1,4]**	**/2**	**/4**	**/8**	**× 1**	**× 1.5**	**× 2**	**× 2.5**	**× 3**
25.0	0	1	2	5	500	125	250	62.5	31.3	15.6	—	—	—	—	375
25.0	0	1	2	6	600	150	300	75 [6]	37.5	18.8	—	—	—	375	450
33.3	0	1	2	5	667	167	333	83.3 [6]	41.6	20.8	—	—	333	416	500
33.3	0	1	2	4	533	133	267	66.7	33.3	16.7	—	—	—	333	400

Table 81. Package Thermal Characteristics for TePBGA II (continued)

Parameter	Symbol	Value	Unit	Note
Junction-to-package natural convection on top	ψ_{JT}	6	°C/W	6

Notes:
1. Junction temperature is a function of die size, on-chip power dissipation, package thermal resistance, mounting site (board) temperature, ambient temperature, air flow, power dissipation of other components on the board, and board thermal resistance.
2. Per JEDEC JESD51-2 with the single layer board horizontal. Board meets JESD51-9 specification.
3. Per JEDEC JESD51-6 with the board horizontal.
4. Thermal resistance between the die and the printed circuit board per JEDEC JESD51-8. Board temperature is measured on the top surface of the board near the package.
5. Thermal resistance between the die and the case top surface as measured by the cold plate method (MIL SPEC-883 Method 1012.1).
6. Thermal characterization parameter indicating the temperature difference between package top and the junction temperature per JEDEC JESD51-2. When Greek letters are not available, the thermal characterization parameter is written as Psi-JT.

24.2 Thermal Management Information

For the following sections, $P_D = (V_{DD} \times I_{DD}) + P_{I/O}$ where $P_{I/O}$ is the power dissipation of the I/O drivers.

24.2.1 Estimation of Junction Temperature with Junction-to-Ambient Thermal Resistance

An estimation of the chip junction temperature, T_J, can be obtained from the equation:

$$T_J = T_A + (R_{\theta JA} \times P_D)$$

where:

T_J = junction temperature (°C)

T_A = ambient temperature for the package (°C)

$R_{\theta JA}$ = junction to ambient thermal resistance (°C/W)

P_D = power dissipation in the package (W)

The junction to ambient thermal resistance is an industry-standard value that provides a quick and easy estimation of thermal performance. Generally, the value obtained on a single layer board is appropriate for a tightly packed printed circuit board. The value obtained on the board with the internal planes is usually appropriate if the board has low power dissipation and the components are well separated. Test cases have demonstrated that errors of a factor of two (in the quantity $T_J - T_A$) are possible.

24.2.2 Estimation of Junction Temperature with Junction-to-Board Thermal Resistance

NOTE

The heat sink cannot be mounted on the package.

The thermal resistance is expressed as the sum of a junction to case thermal resistance and a case-to-ambient thermal resistance:

$$R_{\theta JA} = R_{\theta JC} + R_{\theta CA}$$

where:

$R_{\theta JA}$ = junction to ambient thermal resistance (°C/W)

$R_{\theta JC}$ = junction to case thermal resistance (°C/W)

$R_{\theta CA}$ = case to ambient thermal resistance (°C/W)

$R_{\theta JC}$ is device-related and cannot be influenced by the user. The user controls the thermal environment to change the case to ambient thermal resistance, $R_{\theta CA}$. For instance, the user can change the size of the heat sink, the air flow around the device, the interface material, the mounting arrangement on printed circuit board, or change the thermal dissipation on the printed circuit board surrounding the device.

This first-cut approach overestimates the heat sink size required, since heat flow through the board is not accounted for, which can be as much as one-third to one-half of the power generated in the package.

Accurate thermal design requires thermal modeling of the application environment using computational fluid dynamics software which can model both the conduction cooling through the package and board and the convection cooling due to the air moving through the application. Simplified thermal models of the packages can be assembled using the junction-to-case and junction-to-board thermal resistances listed in the thermal resistance table. More detailed thermal models can be made available on request.

The thermal performance of devices with heat sinks has been simulated with a few commercially available heat sinks. The heat sink choice is determined by the application environment (temperature, air flow, adjacent component power dissipation) and the physical space available. Because of the wide variety of application environments, a single standard heat sink applicable to all cannot be specified.

These capacitors should have a value of 0.01 or 0.1 µF. Only ceramic SMT (surface mount technology) capacitors should be used to minimize lead inductance, preferably 0402 or 0603 sizes.

In addition, it is recommended that there be several bulk storage capacitors distributed around the PCB, feeding the VDD, OVDD, GVDD, and LVDD planes, to enable quick recharging of the smaller chip capacitors. These bulk capacitors should have a low ESR (equivalent series resistance) rating to ensure the quick response time necessary. They should also be connected to the power and ground planes through two vias to minimize inductance. Suggested bulk capacitors—100–330 µF (AVX TPS tantalum or Sanyo OSCON).

25.3 Connection Recommendations

To ensure reliable operation, it is highly recommended that unused inputs be connected to an appropriate signal level. Unused active low inputs should be tied to OVDD, GVDD, or LVDD as required. Unused active high inputs should be connected to GND. All NC (no-connect) signals must remain unconnected.

Power and ground connections must be made to all external VDD, GVDD, LVDD, OVDD, and GND pins of the device.

25.4 Output Buffer DC Impedance

The device drivers are characterized over process, voltage, and temperature. For all buses, the driver is a push-pull single-ended driver type (open drain for I^2C).

To measure Z_0 for the single-ended drivers, an external resistor is connected from the chip pad to OVDD or GND. Then, the value of each resistor is varied until the pad voltage is $OV_{DD}/2$ (see Figure 66). The output impedance is the average of two components, the resistances of the pull-up and pull-down devices. When data is held high, SW1 is closed (SW2 is open) and R_P is trimmed until the voltage at the pad equals $OV_{DD}/2$. R_P then becomes the resistance of the pull-up devices. R_P and R_N are designed to be close to each other in value. Then, $Z_0 = (R_P + R_N)/2$.

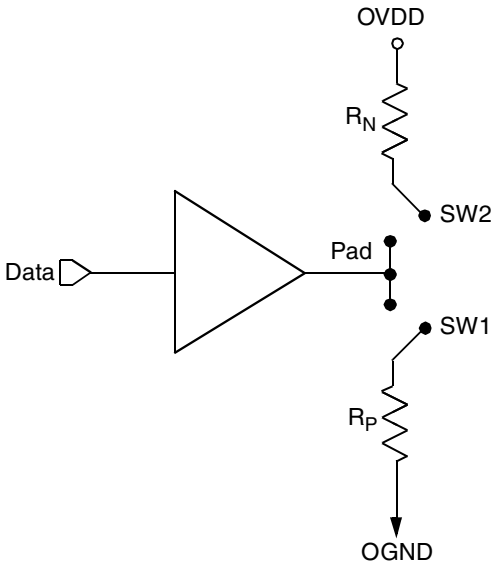

Figure 66. Driver Impedance Measurement